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## Comparison of Nonlinear Filtering Methods for Battery State of Charge Estimation

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# Comparison of Nonlinear Filtering Methods for Battery State of Charge Estimation

A Thesis

Submitted to the Graduate Faculty of the  
University of New Orleans  
in partial fulfillment of the  
requirements for the degree of

Master of Science  
in  
Engineering  
Electrical Engineering

by  
Klaus Zhang  
B.S. Pennsylvania State University, 2011

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# Dedication

I dedicate this thesis to my wife, Elyssa Okkelberg. I wouldn't have been able to finish this project without her love and support. You are my soul mate, and I love you with all my heart.

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# Abstract

In battery management systems, the main figure of merit is the battery's SOC, typically obtained from voltage and current measurements. Present estimation methods use simplified battery models that do not fully capture the electrical characteristics of the battery, which are useful for system design. This thesis studied SOC estimation for a lithium-ion battery using a nonlinear, electrical-circuit battery model that better describes the electrical characteristics of the battery. The extended Kalman filter, unscented Kalman filter, third-order and fifth-order cubature Kalman filter, and the statistically linearized filter were tested on their ability to estimate the SOC through numerical simulation. Their performances were compared based on their root-mean-square error over one hundred Monte Carlo runs as well as the time they took to complete those runs. The results show that the extended Kalman filter is a good choice for estimating the SOC of a lithium-ion battery.

Keywords: nonlinear filtering; battery health management; state of charge estimation

# Introduction

Batteries, particularly rechargeable ones, are used extensively in daily life. They provide the energy for such electrical systems as communication, automotive, and renewable power systems. In order to design for and operate these systems, an accurate battery model and a means of simulating the model efficiently are needed. For example, modern battery charge and health management schemes use high-fidelity battery models to track the state of charge (SOC) and state of health (SOH); this information is then used to predict and optimize the runtime of the battery. However, widely-used chemical batteries have nonlinear capacitive effects, which require the use of a nonlinear filter for accurate prediction of their states in the presence of noise. This thesis explores one possible solution to this problem by choosing an appropriate battery model and testing the accuracy and speed of various nonlinear filters in determining the SOC through simulation. Note that only filters using point-based numerical approximation methods were studied, as opposed to those using density-based methods. See [1] for more information about the differences between various numerical approximation methods in relationship to Bayesian filtering.

## 1.1 Electrical Characteristics of Rechargeable Batteries

A high-fidelity battery model has to accurately reproduce the various characteristics of a battery. Most models keep track of the total capacity and SOC in order to predict remaining runtime. More accurate models include nonlinear effects, such as the rate-capacity effect and the recovery effect, along with self-discharge and the effects of ambient temperature. The dynamic electrical attributes, such as the current-voltage (I-V) characteristics and transient responses, can also be modeled. The remainder of this section defines these characteristics.

The capacity of a battery is the amount of electric charge it can store, measured in the SI unit Ampere-hours (Ah). Commonly, for rechargeable battery specifications, the subunit milliampere-hour (mAh) is used instead. Related is the available capacity, which is the amount of charge that the battery can currently deliver. Due to the electrochemical nature of batteries, a battery's available capacity decreases as the rate of discharge increases, which is known as the rate-capacity effect. Therefore, the capacity for a battery is typically stated for a given discharge rate. Related to this is the recovery effect, so called because when a battery is allowed to rest during an idle period, the battery "recovers" available capacity previously lost during discharge because of the rate-capacity effect. Thus, a battery that is discharged at a high rate until its available capacity reaches zero, when allowed to rest, regains a portion of its lost capacity.

Both the rate-capacity effect and the recovery effect can be explained by the electrochemical nature of the battery. During discharge, the concentration of the active material around the electrode is depleted, and the active materials

in the depletion region move towards the electrode to reduce the concentration gradient [2]. Because the speed at which the concentration gradient is equalized is limited, the faster the rate of discharge, the less the active material is replenished, resulting in a decrease in the available capacity. Likewise, when the battery is allowed to rest, the active material gradient has additional time to equalize, and the available capacity is increased.

Closely related to the capacity is the SOC. This thesis defines it as the ratio between the remaining capacity and the maximum capacity, with both capacities measured using the total amount of active material within the battery. Thus, this definition denotes the proportion of remaining chemical energy rather than the available chemical energy and is unaffected by the rate-capacity and recovery effects. Note that a fully charged battery has an SOC of unity and a fully discharged battery has an SOC of zero, regardless of the available capacity. Additionally, there exists a nonlinear relationship between the SOC of the battery and its open-circuit voltage  $V_{OC}$ , which is useful for simulation of the I-V characteristics and transient responses. The  $V_{OC}$  is the limit of the measured battery voltage after recovery, assuming no self-discharge.

Other, more minor effects that are commonly modeled are self-discharge, the effect of ambient temperature, and aging. Self-discharge refers to the decrease of an idle battery's SOC over time due to internal chemical reactions. It is dependent on the type of battery, SOC, ambient temperatures, and other factors. The ambient temperature has effects on the internal resistance of the battery and the self-discharge rate. Commonly, the battery is designed to operate within a narrow range of temperatures. Below the operating temperature range, the internal resistance increases, decreasing the capacity. Above the operating range, the internal resistance decreases, not only increasing the capacity but also the self-

discharge rate; thus, the deliverable capacity is lowered due to the increased self-discharge. Aging refers to the decrease in battery performance measures, such as capacity, self-discharge, and internal resistance, over time due to unwanted chemical reactions. In practice, aging is indicated by the SOH, defined as the ratio between the current maximum capacity and that of a new battery. The SOH threshold at which the battery performance is considered too degraded varies by application.

This thesis is mainly concerned with estimating the SOC from noisy measurements. The SOH is easier to estimate as it changes slowly over charge cycles, rather than within each charge cycle. Additionally, no simplified expressions exist for the SOH, so it is usually determined empirically. Thus, only the estimation of the SOC was studied by this paper.

## **1.2 Battery Models**

This thesis studied the estimation of the SOC of a battery given knowledge of the resistive load on the battery as well as noisy measurements of the voltage across its terminals. A known resistive load profile, rather than the current, was used because in a real-life usage, it is difficult to exactly control the current drawn by a load. In order to estimate the SOC for a general load profile, incorporation of the rate-capacity and recovery effects as well as the transient I-V characteristics is desirable. Furthermore it is useful to have a model easily tunable for different battery types. To find a battery model that meets these goals, the major types of battery models are reviewed and their characteristics are compared. Jongerden and Haverkort determined four main categories for battery models, namely electrochemical, analytical, stochastic, and electrical-circuit [3]. Additionally, battery

models that use computational intelligence exist, e.g. [4–8]. The remainder of this section reviews these five types and determines the most suitable battery model for this study.

### 1.2.1 Electrochemical

Electrochemical models describe the chemical processes that take place in the battery in great detail. These are generally the most accurate, but they require in-depth knowledge of the chemical processes to create and impose large computational costs [9]. One of the most widely known electrochemical models was developed by Doyle, Fuller, and Newman for lithium and lithium-ion batteries using noninvasive voltage-current cycling experiments [10–12]. It consists of six coupled, nonlinear differential equations that capture lithium diffusion dynamics and charge transfer kinetics. The model is able to predict I-V response and provides a design guide for thermodynamics, kinetics, and transport across electrodes. A implementation of their model in Fortran, called Dualfoil, is available for free online.<sup>1</sup> The program needs more than 60 parameters along with the load profile in order to compute the battery properties. Setting the parameters requires detailed knowledge of the battery, but as a result, the program is highly accurate. It is so accurate that other battery models are often compared to it rather than to experimental results.

### 1.2.2 Computational Intelligence

Computational intelligence is a branch of computer science interested in problems that require the intelligence of humans and animals to solve. One of the earliest definitions by Bezdek states that computational intelligent systems use pattern

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<sup>1</sup>J. Newman, *Fortran programs for the simulation of electrochemical systems*, <http://www.cchem.berkeley.edu/jsngrp/fortran.html>, 1998.

recognition on low-level, numerical data and do not use knowledge as with artificial intelligence [14, 15]. Methods such as neural networks, fuzzy systems, and evolutionary computation are commonly classified as computational intelligence. Battery models using such methods as neural networks [5, 6], support vector machines [7], and hybrid neural-fuzzy models [8] have been studied. These models learn the nonlinear relationships between battery properties, such as SOC, current, voltage, and temperature, through a computationally costly training process. However, once trained, they incur a much lower cost and can achieve comparable accuracy to electrochemical models.

### 1.2.3 Analytical

Analytical models are simplified electrochemical models that trade off accuracy for simplicity. One of the simplest such models is Peukert's law for lead-acid batteries, which states that for a one-ampere discharge rate [16]

$$C_p = I^k t, \quad (1.1)$$

where  $C_p$  is the capacity at a one-ampere discharge rate in Ah,  $I$  is the discharge current in A,  $t$  is the time to discharge the battery in hours, and  $k \geq 1$  is the dimensionless Peukert constant, typically between 1.1 and 1.3 for a lead-acid battery. The constant  $k$  only equals unity for an ideal accumulator, so for real batteries,  $k$  is always greater than unity. Thus, for a given increase in the discharge current, the discharge time decreases by a proportionally greater amount. Therefore, the effective, or available, capacity  $C \times t$  is reduced. Peukert's law can be extended to some other battery chemistries, such as lithium-ion [16]. Note that Peukert's law models only the rate-capacity effect and not the recovery effect. More complicated

models, such as the kinetic battery model and the diffusion model, are able to describe both effects.

The kinetic battery model (KiBaM), initially created for large lead-acid batteries, describes the battery as a kinetic process, using two charge wells for the bound and available charges connected by a valve whose flow rate is proportional to the height difference between the wells [17]. The change of charge in the wells is given by

$$\begin{cases} \frac{dy_1}{dt} = -I + k(h_2 - h_1) \\ \frac{dy_2}{dt} = -k(h_2 - h_1), \end{cases} \quad (1.2)$$

where  $y_1, y_2$  are the charges,  $h_1, h_2$  are the heights of the wells, the parameter  $k$  controls the rate of charge flow between the wells, and  $I$  is the applied load. The flow rate of the valve should be lower than the typical discharge rate of the battery. During discharge from the available-charge well, the bound charges flow through the valve to equalize the heights of the two wells. It can be seen that for slower discharge rates, more charge flows through the valve and the effective capacity increases. Likewise, during idle periods, the battery recovers available charge.

Related to the KiBaM is the diffusion model, which describes the movement of the ions in the electrolyte of a lithium-ion battery [18]. Like in the kinetic battery model, the difference in the concentration of adjacent ions along the length of the battery determines the diffusion rate of the ions. The available charges are those ions directly touching the electrode of the battery. It can be seen that the KiBaM is a first-order approximation of the diffusion model [9], since the individual ions in the diffusion model are replaced by two charge wells in the KiBaM.



### 1.2.4 Stochastic

Stochastic models describe the discharging and the recovery effect as stochastic processes. The first models were developed by Chiasserini and Rao and based on discrete-time Markov chains [19]. They studied two models of a battery in a communication device that transmitted packets. The simpler model described the battery as a discrete-time Markov chain with  $N+1$  states, numbered from 0 to  $N$  and corresponding to the number of charge units available in the battery. Transmitting one packet requires one charge unit of energy. Thus, in continuous transmission,  $N$  packets can be sent. At every time step, a charge unit is either consumed with probability  $a_1 = q$  or recovered with probability  $a_0 = 1 - q$ . The battery is considered empty when the 0 state is reached or when a theoretical maximum of  $T$  charge units have been consumed. The second model is an extension of the first, allowing for more than one charge unit to be consumed in a time step, modeling more bursty usage. Additionally, the battery has a non-zero probability of staying in the same charge state, indicating no consumption or recovery during a time step. Chiasserini and Rao extended their model further in following papers by adding state and phase dependence [2, 20, 21]. The state number is the number of charge units, and the phase number is the number of consumed charge units. Having fewer charge units decreases the probability of recovery, while having more consumed charge units increases the probability of recover. Using these models, one can model different loads by setting the transition probabilities. However, the order of the transitions is uncontrollable, so it is impossible to model fixed load patterns and compute their impact on battery life.

Chiasserini and Rao mainly investigated the gain  $G$  in transmitted packets using a pulsed discharge relative to using a constant discharge, defined as  $G = m/N$ ,

where  $m$  is the mean number of transmitted packets. The gain increases when the load decreases, due to an increase in the recovery probability. Additionally, the gain increases for lower discharge demand rates and higher current densities. These load profiles result in discharge currents close to the specified limits of the battery, causing the available capacity to decrease overly quickly. Therefore, the recovery effect is especially strong for these cases during pulsed discharge, greatly increasing the gain. Chiasserini and Rao compared the computation of the gain parameter for different current densities and demand rates using the stochastic model to that of the electrochemical model of Doyle et al. They found an average deviation of 1% and a maximum deviation of 4%. This shows that the stochastic model accurately describes battery behavior during pulsed discharge. However, this model is only able to compute relative lifetimes.

In 2005, Rao et al. [22] proposed a stochastic battery model for a nickel-metal hydride (NiMH) battery based on the Kinetic Battery Model (KiBaM) of Manwell and McGowan. The differential equations governing the original KiBaM were modified to include an extra factor  $h_2$  governing the flow of charge between the wells. This changes Equation (1.2) into

$$\begin{cases} \frac{dy_1}{dt} = -I + k_s h_2 (h_2 - h_1) \\ \frac{dy_2}{dt} = -k_s h_2 (h_2 - h_1), \end{cases} \quad (1.3)$$

This change causes the recovery effect to weaken as the remaining charge decreases. The stochastic model was also modified to allow the possibility of no recovery during idle periods. The stochastic KiBaM describes the battery using a discrete-time, transient Markov process. The states are labeled with the parameters  $(i, j, t)$ , with  $i$  and  $j$  representing the discrete charge levels of the available and bound

charge wells and  $t$  representing the length of the current idle period. Like the stochastic model of Chiasserini and Rao, it is impossible to fully model a real-life discharge pattern using the stochastic KiBaM. Rao et al. compared the results of their model with experimental results using an AAA NiMH battery. Two sets of experiments were conducted, the first with varying frequency of the load and a 50% duty cycle and the second with varying off-time and a constant on-time. Their model accurately predicted the lifetime and delivered charge from the battery, with a maximum error of 2.65%.

### 1.2.5 Electrical-Circuit

Electrical-circuit models for batteries developed from the discovery of capacitive effects at the electrode-electrolyte interface. Helmholtz first proposed the existence of a double layer of charge at the interface in 1879. In 1899, Warburg proposed a series resistance and capacitance circuit model with an infinitely low current density. The Warburg capacitance  $C_W$  named after him varies inversely with the square root of the frequency [23]. In 1947, Randles proposed a model consisting of a double-layer polarization capacitance  $C_p$  in parallel with the series combination of a resistor  $R$  and a capacitance  $C$  [24]. In 1994, Kovacs improved Randles circuit with the addition of Warburg impedance  $Z_W$  replacing the capacitance  $C$  and the solution resistance  $R_s$  in series with the original Randles circuit [25]. In addition, he renamed  $C_p$  to the double layer capacitance  $C_{dl}$  and  $R$  to the charge-transfer resistance  $R_{ct}$ . These proposals came from a desire to represent impedance spectra created using electrochemical impedance spectroscopy (EIS). The various elements in the models represent the different processes within a battery, which have different time constants. While these attempts model the impedance and, thus,

account for the nonlinear rate-capacity and recovery effects, they do not consider the capacity and self-discharge of the battery.

In 1993, Hageman created simplified electrical-circuit models using PSpice for nickel-cadmium (NiCd), lead-acid, and alkaline batteries [26]. The circuits shared the common elements of *i*) a capacitor that represents the battery capacity, *ii*) a discharge rate normalizer that determines the additional capacity loss at high discharge rates, *iii*) a circuit that discharges the battery, *iv*) a lookup table of battery voltage versus SOC, and *v*) a resistor that represents the battery's internal resistance [26, 27]. In addition, battery models for NiCd batteries simulated the thermal effects under high discharge rates. The main lookup table is formed by discharging a battery at a low rate at a constant current (20 to 200 hours). At high discharge rates, the discharge rate normalizer reduces the battery voltage below the value from looking up the SOC in the table. This normalizer is implemented using additional lookup tables. These circuit models were much simpler than electrochemical models, but they were also less accurate with an approximate error of 10%. Furthermore, creation of the lookup tables requires considerable data. These circuit-based models were used to estimate the remaining discharge time and are referred to as runtime-based models.

In 2006, Chen and Rincón-Mora proposed a combination of a runtime-based model and an impedance-based model consisting of a series resistor and two parallel resistor-capacitor networks [28]. A schematic for their model is shown in Figure 2.1. The elements of the impedance part of the model had parameters that depended on the SOC. Additionally, the runtime model included a resistance that modeled the self-discharge rate. Their proposed model has the advantage of accurate prediction of the SOC using the runtime-based portion while also modeling nonlinear transient effects, such as the rate-capacity and recover effects, with the impedance-based

portion. Furthermore, the battery data can be collected using EIS measurements, which requires neither detailed knowledge of the battery chemistry nor lengthy, low-rate discharge experiments.

### 1.2.6 Evaluation

Of the model types, only some are fit for use with filtering algorithms. The computational-intelligence and stochastic models do not adequately describe the dynamics of the battery system for use in the filters covered by this study. On the other hand, electrochemical, analytical, and electrical-circuit models do describe the system dynamics in a compatible manner. Furthermore, they model the nonlinear rate-capacity and recovery effects. Of these, only the electrical-circuit model has the advantage of modeling the internal impedance of the battery, which is useful in the design of battery systems. The relevant characteristics of the model types are summarized in Table 1.1. It can be seen that electrical-circuit models are the most suitable for this study. Among them, the proposal by Chen and Rincón-Mora is most appropriate for the purposes of this thesis, because it is the only one discussed by this paper that describes both the capacity and the transient effects. Therefore, their proposed model is used for simulating the battery and comparing the performance

Table 1.1: Summary of relevant characteristics of various battery model types.

Model Type	Dynamics	Nonlinear Effects	Transient Effects	I-V Characteristics	Design Difficulty
Electrochemical	Y	Y	Y	N	High
Computational Intelligence	N	Y	Y	N	High
Analytical	Y	Y	N	N	Low
Stochastic	N	Y	N	N	Low
Electrical-Circuit	Y	Y	Y	Y	Medium

of different filters.

## 1.3 Nonlinear Filtering Methods

Filtering refers to the methodology for estimating the state of a time-varying system that is indirectly observed through noisy measurements. Specifically, the state at the current time is estimated using the measurements from the current and previous times. The state of a system is a group of dynamic variables that evolve through time, and its evolution through time is governed by a dynamic system, perturbed by process noise. The measurements are functions of the state and the measurement noise.

Systems are classified as either linear or nonlinear. The state dynamics and measurements of a linear system are linear functions of the state, inputs, and noises. Particularly, the superposition principles of additivity and homogeneity are satisfied by a linear system. Nonlinear systems do not satisfy the principle of superposition because the functions defining the systems are not all linear, i.e. some are nonlinear. A battery can be modeled as a nonlinear, time-varying system, with state variables that describe such states as the SOC and the SOH. The measurements are typically the voltage and the current. Note that the SOH was not considered by this thesis for reasons described in Section 1.1, so this thesis assumes the battery system is time-invariant. Additionally, only the voltage was measured since a known resistive load was used as an input to the system in place of the current measurement. This replacement was done because a piecewise constant discharge profile is convenient for simulation purposes and it is more realistic to have a constant discharge load than a constant discharge current. A state-space representation of the battery system proposed by Chen and Rincón-Mora in [28] is described in more detail in

the following chapter.

For linear systems, the optimal filtering solution with respect to the minimum mean squared error (MMSE) is given by the least squares solution, meaning the least squares solution equals the posterior mean. For the Gaussian case, the best estimate is given by a linear MMSE (LMMSE) estimator, of which the Wiener filter for wide-sense stationary signals [29] is an example. In 1960, Kalman generalized Wiener filtering to non-stationary, discrete-time signals [30], with continuous-time versions derived later on. Like the Wiener filter, the Kalman filter is a sequential, LMMSE estimator. For the special case of Gaussian noise, the Kalman filter is the MMSE estimator. Its solution procedure is as follows. Consider a linear system in discrete time with  $n$  states and  $m$  measurements defined by

$$\mathbf{x}_k = F_k \mathbf{x}_{k-1} + B_k \mathbf{u}_k + L \mathbf{w}_k \quad (1.4)$$

$$\mathbf{z}_k = H_k \mathbf{x}_k + M \mathbf{v}_k, \quad (1.5)$$

where  $\mathbf{x} \in \mathbb{R}^n$ ,  $\mathbf{u} \in \mathbb{R}^{N_u}$ , and  $\mathbf{z} \in \mathbb{R}^m$  are vectors of the state variables, known inputs, and measurements, respectively;  $\mathbf{w} \sim \mathcal{N}(0, Q_k)$ ,  $Q_k \in \mathbb{R}^{N_w \times N_w}$ , and  $\mathbf{v} \sim \mathcal{N}(0, R_k)$ ,  $R_k \in \mathbb{R}^{N_v \times N_v}$  are normally distributed noise variables;  $F \in \mathbb{R}^{n \times n}$ ,  $B \in \mathbb{R}^{n \times N_u}$ ,  $H \in \mathbb{R}^{m \times n}$ ,  $L \in \mathbb{R}^{n \times N_w}$ , and  $M \in \mathbb{R}^{m \times N_v}$  are matrices; and a subscript  $k$  on a variable indicates the value of that variable at time  $t_k$ , where  $t_k = t_0 + k\delta$  and  $\delta$  is the time step. First, the Kalman filter propagates the estimates of the state variables  $\hat{\mathbf{x}}$  and the estimation covariances  $P \in \mathbb{R}^{n \times n}$  according to

$$\hat{\mathbf{x}}_{k|k-1} = F_k \hat{\mathbf{x}}_{k-1|k-1} + B_k \mathbf{u}_k \quad (1.6)$$

$$P_{k|k-1} = F_k P_{k-1|k-1} F_k^\top + L Q_k L^\top, \quad (1.7)$$

where  $\hat{(\cdot)}$  indicates the estimated value. Then, the estimates are updated using the measurements according to

$$\tilde{\mathbf{z}}_k = \mathbf{z}_k - H_k \hat{\mathbf{x}}_{k|k-1} \quad (1.8)$$

$$S_k = H_k P_{k|k-1} H_k^\top + M R_k M^\top \quad (1.9)$$

$$K_k = P_{k|k-1} H_k^\top S_k^{-1} \quad (1.10)$$

$$\hat{\mathbf{x}}_{k|k} = \hat{\mathbf{x}}_{k|k-1} + K_k \tilde{\mathbf{z}}_k \quad (1.11)$$

$$P_{k|k} = (I - K_k H_k) P_{k|k-1}. \quad (1.12)$$

Note that it was assumed the noises were Gaussian. Under this assumption, the Kalman filter produces the optimal solution in the maximum likelihood (ML) and the maximum a posterior (MAP) senses, in addition to in the MMSE sense. However, the Gaussian assumption is unnecessary for the Kalman filter to produce the LMMSE estimate for a general linear system.

For nonlinear systems, optimal filtering solutions are generally intractable, so various numerical approximation methods have been developed. Chen describes seven categories of such methods, namely Gaussian/Laplace approximation, iterative quadrature, multigrid method and point-mass approximation, moment approximation, Gaussian sum approximation, deterministic sampling approximation, and Monte Carlo sampling approximation [1]. Note that only filters using point-based numerical approximation methods were studied, as opposed to those using density-based methods. This was done because typical battery management systems do not have the computational power to employ costly density-based methods, and point-based methods use the simple LMMSE update of the Kalman filter. Point-based and density-based methods are also known as local and global



approaches, respectively. Additionally, only filters using methods from the two most popular categories of Gaussian approximation and deterministic sampling approximation [31] were used to further limit the scope of this study.

Gaussian approximation operates by assuming the posterior distribution is Gaussian. Then, the Taylor-series-based extended Kalman filter (EKF) [32] or the Gaussian-describing-function-based statistically linearized filter (SLF) [33] can be used. Li and Jilkov state that the EKF approximates the nonlinear dynamic and measurement functions, while the SLF simplifies the nonlinear stochastic system to a linear system so that linear filtering results are applicable [31]. Deterministic sampling methods are special numerical methods that estimate the mean and covariance. This category includes the unscented Kalman filter (UKF) [34] and the cubature Kalman filter (CKF) [35]. The main advantage of the deterministic sampling methods is they are derivative-free. The remainder of this section details the general implementation of these filters for a discrete-time system of the form

$$\mathbf{x}_k = \mathbf{f}_d(\mathbf{x}_{k-1}, \mathbf{u}_k) + L(\mathbf{x}_{k-1}, \mathbf{u}_k)\mathbf{w}_k \quad (1.13)$$

$$\mathbf{z}_k = \mathbf{h}(\mathbf{x}_k, \mathbf{u}_k) + M(\mathbf{x}_k, \mathbf{u}_k)\mathbf{v}_k, \quad (1.14)$$

where  $\mathbf{f} \in \mathbb{R}^n$  and  $\mathbf{h} \in \mathbb{R}^m$  are nonlinear vector functions,  $L \in \mathbb{R}^{n \times N_w}$  and  $M \in \mathbb{R}^{m \times N_v}$  are nonlinear matrix functions, and the input  $\mathbf{u}$  is assumed to be piecewise constant, meaning  $\mathbf{u}(t) = \mathbf{u}(t_k) = \mathbf{u}_k$  for  $t_{k-1} < t \leq t_k$ . An implicit, first-order Taylor-Heun numerical integration method was used to discretize the continuous-time dynamics  $\mathbf{f}$  of the chosen battery model. In particular, an iterated integration procedure was used, as was done by Särkkä [36]. For the iterations, a superscript of  $(i)$  indicates the  $i$ th step of a  $M$ -step iterative integration scheme. Note that  $\hat{\mathbf{x}}_{k-1}^{(0)} = \hat{\mathbf{x}}_{k-1}$  and  $\hat{\mathbf{x}}_{k-1}^{(M)} = \hat{\mathbf{x}}_k$ . The specifics of the discretization along with the

notation used are discussed in Section 2.2.

### 1.3.1 Extended Kalman Filter

One of the most popular nonlinear filters is the extended Kalman filter (EKF), which approximates the nonlinear state and measurement functions using Taylor series expansion. This study uses the first-order expansion for the EKF. The prediction step follows the discretization approach proposed by Mazzoni [37] to numerically approximate the continuous-time dynamics in Equation (2.35) and the continuous-time estimate covariance differential equation

$$\dot{P} = F(\mathbf{x}, \mathbf{u})P + PF^\top(\mathbf{x}, \mathbf{u}) + L(\mathbf{x}, \mathbf{u})QL^\top(\mathbf{x}, \mathbf{u}), \quad (1.15)$$

with the Jacobian  $F = \partial f / \partial \mathbf{x}$ . The discretization  $\mathbf{f}_d$  of  $\mathbf{f}$  is given in Section 2.2, and the discretion of the estimate covariance matrix is as follows. Note that an  $M$ -step iterative integration method was used for the discretization of  $\mathbf{f}$ . Thus, a similar iterative procedure was used for the discretion of the estimate covariance matrix. For a time step of  $\delta = (t_k - t_{k-1})/M$ , where  $M$  is a positive integer, the prediction step consists of  $M$  iterations of the following equations:

$$\hat{\mathbf{x}}_{k-1|k-1}^{(i)} = \mathbf{f}_d(\hat{\mathbf{x}}_{k-1}^{(i-1)}, \mathbf{u}_k, \delta, i) \quad (1.16)$$

$$P_{k-1|k-1}^{(i)} = P_{k-1|k-1}^{(i-1)} + G_\tau \left\{ F(\hat{\mathbf{x}}_\tau, \mathbf{u}_k) P_{k-1|k-1}^{(i-1)} + P_{k-1|k-1}^{(i-1)} F^\top(\hat{\mathbf{x}}_\tau, \mathbf{u}_k) + L(\hat{\mathbf{x}}_\tau, \mathbf{u}_k) Q_\tau L^\top(\hat{\mathbf{x}}_\tau, \mathbf{u}_k) \right\} G_\tau^\top \delta, \quad (1.17)$$

where  $t_\tau = t_{k-1} + \delta(i + 1/2)$ ,

$$G_\tau = \left( I - F(\hat{\mathbf{x}}_\tau, \mathbf{u}_k) \frac{\delta}{2} \right)^{-1}, \quad (1.18)$$

and

$$\hat{\mathbf{x}}_\tau = \frac{1}{2} \left( \hat{\mathbf{x}}_{k-1}^{(i-1)} + \hat{\mathbf{x}}_{k-1}^{(i)} - F(\hat{\mathbf{x}}_{k-1}^{(i)}, \mathbf{u}_k) f(\hat{\mathbf{x}}_{k-1}^{(i)}) \frac{\delta^2}{4} \right). \quad (1.19)$$

The iteration given by Equations (1.16) and (1.17) is repeated  $M$ -times to complete the prediction step. It can be seen that the differential equation for the covariance matrix was approximated using a modified Gauss-Legendre formula with an implicit increment rule, following Mazzoni. The numerical approximations for the state and covariance are both A-stable, which is necessary for the chosen battery model, and consistent to the first-order. The update equations for the EKF come from the LMMSE filter and are

$$K_k = P_{k|k-1} H_k^\top (H_k P_{k|k-1} H_k^\top + M(\hat{\mathbf{x}}_k) R_k M^\top(\hat{\mathbf{x}}_k))^{-1} \quad (1.20)$$

$$\hat{\mathbf{x}}_{k|k} = \hat{\mathbf{x}}_{k|k-1} + K_k (\mathbf{z}_k - \mathbf{h}(\hat{\mathbf{x}}_{k|k-1})) \quad (1.21)$$

$$P_{k|k} = (I - K_k H_k) P_{k|k-1}, \quad (1.22)$$

with the Jacobian  $H = \partial \mathbf{h} / \partial \mathbf{x}$ .

### 1.3.2 Unscented Kalman Filter

The unscented Kalman filter (UKF) is an efficient, generally derivative-free filtering algorithm that relies on the unscented transformation (UT). The UT is useful for forming the Gaussian approximation to the joint distribution of random variables  $x$  and  $y$  for  $x \sim \mathcal{N}(m, P)$  and  $y = g(x)$ , where  $x \in \mathbb{R}^n$ ,  $y \in \mathbb{R}^m$ , and  $g : \mathbb{R}^n \mapsto \mathbb{R}^m$  is a nonlinear function. Then, the first and second moments corresponding to the mean and covariance can be easily found. Specifically, suppose the Gaussian

approximation of the joint probability density of  $x$  and  $y$  has the form

$$\begin{bmatrix} x \\ y \end{bmatrix} = \mathcal{N} \left( \begin{bmatrix} m \\ \mu_U \end{bmatrix}, \begin{bmatrix} P & C_U \\ C_U^\top & S_U \end{bmatrix} \right). \quad (1.23)$$

Then, the UT picks  $2n + 1$  sample points  $\{x_i\}$ , commonly known as sigma points, along with the same number of weights  $\{w_i\}$ , as follows [38]. First, the sigma points are chosen from the columns of the matrix  $\sqrt{(n + \lambda)P}$ , giving

$$x^{(0)} = m_x \quad (1.24)$$

$$x^{(i)} = m_x + \left[ \sqrt{(n + \lambda)P} \right]_i, \quad i = 1, \dots, n \quad (1.25)$$

$$x^{(i)} = m_x - \left[ \sqrt{(n + \lambda)P} \right]_{i-n}, \quad i = n + 1, \dots, 2n \quad (1.26)$$

with the weights

$$W_0^{(m)} = \frac{\lambda}{n + \lambda} \quad (1.27)$$

$$W_0^{(c)} = \frac{\lambda}{n + \lambda} + (1 - \alpha^2 + \beta) \quad (1.28)$$

$$W_i^{(m)} = W_i^{(c)} = \frac{1}{2(n + \lambda)}, \quad i = 1, \dots, 2n. \quad (1.29)$$

The parameter  $\lambda$  is defined as

$$\lambda = \alpha^2(n + \kappa) - n, \quad (1.30)$$

and the constants  $\alpha$ ,  $\beta$ , and  $\kappa$  are parameters of the method. For the UKF,  $\alpha$  is a small positive number, e.g.  $10^{-3}$ ,  $\beta = 2$  is ideal for a Gaussian distribution, and  $\kappa$  is

typically 0. Each sigma point is transformed by

$$y^{(i)} = g(x^{(i)}), \quad i = 0, \dots, 2n. \quad (1.31)$$

Then, the moments are approximated by

$$\mu_U = \sum_{i=0}^{2n} W_i^{(m)} y^{(i)} \quad (1.32)$$

$$S_U = \sum_{i=0}^{2n} W_i^{(c)} (y^{(i)} - \mu_U)(y^{(i)} - \mu_U)^\top \quad (1.33)$$

$$C_U = \sum_{i=0}^{2n} W_i^{(c)} (x^{(i)} - m)(y^{(i)} - \mu_U)^\top. \quad (1.34)$$

The square root of the positive definite matrix  $P$  is defined as a matrix  $A$  such that  $P = AA^\top$ . Note that  $A$  is not unique. For performance reasons, the Cholesky factorization is typically used.

Let the described UT algorithm be denoted by

$$[\mu_U, S_U, C_U] = \text{UT}(g, m, P). \quad (1.35)$$

Then, for the discretized system in Equations (1.13) and (1.14), for an  $M$ -step numerical integration scheme, the prediction step for the UKF can be written as

$$[\hat{\mathbf{x}}_{k-1|k-1}^{(i)}, \tilde{P}_{k-1|k-1}^{(i)}] = \text{UT}(\mathbf{f}_d, \hat{\mathbf{x}}_{k-1|k-1}^{(i-1)}, P_{k-1|k-1}^{(i-1)}) \quad (1.36)$$

$$P_{k-1|k-1}^{(i)} = \tilde{P}_{k-1|k-1}^{(i)} + L(\hat{\mathbf{x}}_{k-1|k-1}^{(i)}) Q_k L^\top(\hat{\mathbf{x}}_{k-1|k-1}^{(i)}), \quad (1.37)$$

$$(1.38)$$

where the equations are performed for  $i = 1, \dots, M$ . Then, the update step is given

by

$$[\mu_k, \tilde{S}_k, C_k] = \text{UT}(\mathbf{h}, \hat{\mathbf{x}}_{k|k-1}, P_{k|k-1}) \quad (1.39)$$

$$S_k = \tilde{S}_k + M(\hat{\mathbf{x}}_{k|k-1})R_kM^\top(\hat{\mathbf{x}}_{k|k-1}) \quad (1.40)$$

$$K_k = C_k S_k^{-1} \quad (1.41)$$

$$\hat{\mathbf{x}}_{k|k} = \hat{\mathbf{x}}_{k|k-1} + K_k(z_k - \mu_k) \quad (1.42)$$

$$P_{k|k} = P_{k|k-1} - K_k S_k K_k^\top. \quad (1.43)$$

Note that the mean and covariances were estimated using the UT, and the update is equivalent to the LMSSE update used in the Kalman filter.

For numerical stability reasons, this study employed a change to the above UKF procedure as suggested by Julier et al. [39]. In Equation (1.36), the covariance is estimated by

$$\tilde{P}_{k|k-1} = \sum_{i=0}^{2n} W_i^{(c)} (\hat{\mathbf{x}}_{k|k-1}^{(i)} - \hat{\mathbf{x}}_{k|k-1}^{(0)}) (\hat{\mathbf{x}}_{k|k-1}^{(i)} - \hat{\mathbf{x}}_{k|k-1}^{(0)})^\top, \quad (1.44)$$

where the covariance is evaluated about the projected mean rather than the weighted mean. This change ensures the positive definiteness of the covariance matrix, as required by the definition of covariance. Another change, discovered by the author, that results in better numerical stability and lower MSE is the estimation of the cross-covariance in Equation (1.39) by

$$C_k = \sum_{i=0}^{2n} W_i^{(c)} (\hat{\chi}_{k|k-1}^{(i)} - \hat{\chi}_{k|k-1}^{(0)}) (\hat{\mathbf{z}}_k^{(i)} - \mu_k)^\top, \quad (1.45)$$

where  $\hat{\chi}_{k|k-1}^{(i)}$  are the sigma points whose weighted average is  $\hat{\mathbf{x}}_{k|k-1}$ . Note that similar to Equation (1.44), the cross-covariance is evaluated about the projected

mean  $\hat{\mathbf{x}}_{k|k-1}^{(0)}$  and the weighted mean  $\mu_k$ . The increase in stability and accuracy with the change in Equation (1.45) was discovered through experimentation. The reason for the improvement is unknown, but the change was used to produce the simulation results.

### 1.3.3 Cubature Kalman Filter

The cubature Kalman filter (CKF) is similar to the UKF except that it uses the spherical-radial cubature rule rather than the UT to approximate the Gaussian integrals. Indeed, the prediction and update steps of the CKF follow Equations (1.36) to (1.43) except that the UT algorithms in Equations (1.36) and (1.39) are replaced by the corresponding cubature algorithm. This thesis explores the third-order and fifth-order CKFs, whose implementations are discussed in the following two sections.

#### 1.3.3.1 Third-Order CKF

The third-order spherical-radial CKF of Arasaratnam et al. [35, 40] is a special case of the UKF with  $\alpha = 1$ ,  $\beta = 0$ , and  $\kappa = 0$ . The third-order cubature rule chooses  $2n$  cubature points, giving [35]

$$x^{(i)} = m_x + \left[ \sqrt{nP} \right]_i, \quad i = 1, \dots, n \quad (1.46)$$

$$x^{(i)} = m_x - \left[ \sqrt{nP} \right]_{i-n}, \quad i = n+1, \dots, 2n, \quad (1.47)$$

where the matrix square root is computed using Cholesky factorization, as in the UT. Then, the moments are approximated by

$$\mu_U = \frac{1}{2n} \sum_{i=1}^{2n} y^{(i)} \quad (1.48)$$

$$S_U = \frac{1}{2n} \sum_{i=1}^{2n} (y^{(i)} - \mu_U)(y^{(i)} - \mu_U)^\top \quad (1.49)$$

$$C_U = \frac{1}{2n} \sum_{i=1}^{2n} (x^{(i)} - m)(y^{(i)} - \mu_U)^\top. \quad (1.50)$$

The prediction and update steps follow Equations (1.36) to (1.43) with the UTs in Equations (1.36) and (1.39) replaced by the third-order cubature rule given by Equations (1.46) to (1.50). The resulting third-order CKF is exact for polynomials of order three. Compared to the UKF, the third-order CKF is numerically more stable due to its positive weights. While the UKF has some desirable theoretical properties, its weights can be negative, causing numerical problems in some cases [36].

To increase numerical stability and accuracy, a change similar to that in Equation (1.45) was used, giving

$$C_k = \frac{1}{2n} \sum_{i=0}^{2n} (\hat{\chi}_{k|k-1}^{(i)} - \hat{\mathbf{x}}_{k|k-1})(\hat{\mathbf{z}}_k^{(i)} - \mu_k)^\top, \quad (1.51)$$

where  $\hat{\chi}_{k|k-1}^{(i)}$  are the cubature points whose average is  $\hat{\mathbf{x}}_{k|k-1}$ . This change was verified through experimentation to produce better results.

### 1.3.3.2 Fifth-Order CKF

The fifth-order spherical-radial CKF is a higher-order extension of the third-order CKF that is exact for polynomials of order five. Its cubature rule chooses  $2n^2 + 1$



cubature points, giving [41, 42]

$$x^{(0)} = m_x \quad (1.52)$$

$$x^{(i)} = m_x + \left[ \sqrt{n+2} e_i \right], \quad i = 1, \dots, n \quad (1.53)$$

$$x^{(i)} = m_x - \left[ \sqrt{n+2} e_{i-n} \right], \quad i = n+1, \dots, 2n \quad (1.54)$$

$$x^{(i)} = m_x + \left[ \sqrt{n+2} s_{i-2n}^+ \right], \quad i = 2n+1, \dots, 2n + \frac{n(n-1)}{2} \quad (1.55)$$

$$x^{(i)} = m_x - \left[ \sqrt{n+2} s_{i-2n-n(n-1)/2}^+ \right], \quad i = 2n + \frac{n(n-1)}{2} + 1, \dots, 2n + n(n-1) \quad (1.56)$$

$$x^{(i)} = m_x + \left[ \sqrt{n+2} s_{i-2n-n(n-1)}^- \right], \quad i = 2n + n(n-1) + 1, \dots, 2n + \frac{3n(n-1)}{2} \quad (1.57)$$

$$x^{(i)} = m_x - \left[ \sqrt{n+2} s_{i-2n-3n(n-1)/2}^- \right], \quad i = 2n + \frac{3n(n-1)}{2} + 1, \dots, 2n^2, \quad (1.58)$$

where  $e_i$  are the columns of the Cholesky factorization  $\sqrt{P}$  and

$$s_i^\pm = \left\{ \frac{1}{\sqrt{2}} (e_j \pm e_k) : j < k; j, k = 1, 2, \dots, n \right\} \quad (1.59)$$

are scaled linear combinations of the columns  $e_i$ . The weights on the points are

$$W_0 = \frac{2}{n+2} \quad (1.60)$$

$$W_i = \frac{4-n}{2(n+2)^2}, \quad i = 1, \dots, 2n \quad (1.61)$$

$$W_i = \frac{1}{(n+2)^2}, \quad i = 2n+1, \dots, 2n^2. \quad (1.62)$$

Then, moments are approximated by

$$\mu_U = \sum_{i=0}^{2n^2} W_i y^{(i)} \quad (1.63)$$

$$S_U = \sum_{i=0}^{2n^2} W_i (y^{(i)} - \mu_U)(y^{(i)} - \mu_U)^\top \quad (1.64)$$

$$C_U = \sum_{i=0}^{2n^2} W_i (x^{(i)} - m)(y^{(i)} - \mu_U)^\top. \quad (1.65)$$

As in the third-order CKF, the prediction and update steps follow Equations (1.36) to (1.43) with the UTs in Equations (1.36) and (1.39) replaced by the fifth-order cubature rule given by Equations (1.53) to (1.65). Note that unlike the third-order CKF and like the UKF, the weights of the fifth-order CKF can be negative.

As in the third-order CKF, to increase numerical stability and accuracy, a change similar to that in Equation (1.45) was used, giving

$$C_k = \sum_{i=0}^{2n^2} W_i (\hat{\mathbf{x}}_{k|k-1}^{(i)} - \hat{\mathbf{x}}_{k|k-1})(\hat{\mathbf{z}}_k^{(i)} - \mu_k)^\top. \quad (1.66)$$

where  $\hat{\chi}_{k|k-1}^{(i)}$  are the cubature points whose weighted average is  $\hat{\mathbf{x}}_{k|k-1}$ . This change was verified through experimentation to produce better results.

### 1.3.4 Statistically Linearized Filter

In the statistically linearized filter (SLF), the nonlinear state and measurement functions are statistically linearized to minimize the MSE. Then, the resulting linear system can be filtered using the linear Kalman filter. Specifically, given

$\mathbf{x} \sim \mathcal{N}(m, P)$ , the nonlinear function  $\mathbf{f}(\mathbf{x})$  is linearized as [31, 33, 43]

$$\mathbf{f}(\mathbf{x}) \approx \mathbf{b} + A(\mathbf{x} - m), \quad (1.67)$$

where the parameters  $\mathbf{b}$  and  $A$  are chosen to minimize the error

$$\text{MSE}(\mathbf{b}, A) = E [\|\mathbf{f}(\mathbf{x}) - \mathbf{b} - A(\mathbf{x} - m)\|^2]. \quad (1.68)$$

Differentiating the MSE expression and setting the derivatives to zero, produces the optimal values

$$\mathbf{b} = E[\mathbf{f}(\mathbf{x})] \quad (1.69)$$

$$A = E[\mathbf{f}(\mathbf{x})(\mathbf{x} - m)^\top]P^{-1}. \quad (1.70)$$

These values reproduce the mean exactly but the covariance is an approximation. The expectations can be calculated analytically or numerically. Due to the difficulty of finding the analytical forms of the expectations, this study chooses to approximate them numerically using the third-order spherical-radial cubature rule described in Section 1.3.3.1, which has the advantages of numerical stability and low computational complexity compared to the UT and fifth-order cubature rule, respectively. The cubature approximation results in

$$\mathbf{b}_{\mathbf{x}} = E[\mathbf{f}_d(\mathbf{x})] \approx \frac{1}{2n} \sum_{i=1}^{2n} \mathbf{f}_d(\mathbf{x}^{(i)}) \quad (1.71)$$

$$A_{\mathbf{x}} = E[\mathbf{f}(\mathbf{x})(\mathbf{x} - m)^\top]E[(\mathbf{x} - m)(\mathbf{x} - m)^\top]^{-1} = E[F(\mathbf{x})] \approx \frac{1}{2n} \sum_{i=1}^{2n} F(\mathbf{x}^{(i)}) \quad (1.72)$$

for the expectations of the state mean and covariance and

$$\mathbf{b}_z = E[\mathbf{h}(\mathbf{x})] \approx \frac{1}{2n} \sum_{i=1}^{2n} \mathbf{h}(\mathbf{x}^{(i)}) \quad (1.73)$$

$$A_z = E[\mathbf{h}(\mathbf{x})(\mathbf{x} - m)^\top] E[(\mathbf{x} - m)(\mathbf{x} - m)^\top]^{-1} = E[H(\mathbf{x})] \approx \frac{1}{2n} \sum_{i=1}^{2n} H(\mathbf{x}^{(i)}) \quad (1.74)$$

for the expectations of the measurement state and covariance, where the cubature points come from the columns of  $\sqrt{nP}$ . With the given statistically optimal linearization, the resulting linear system can be filtered using a procedure similar to the linear Kalman filter. The prediction phase, for an  $M$ -step numerical integration scheme, consists of performing the following equations  $M$  times for  $i = 1, \dots, M$  using the notation from Section 2.2:

$$\hat{\mathbf{x}}_{k-1|k-1}^{(i)} = \mathbf{b}_{\hat{\mathbf{x}}_{k-1|k-1}^{(i-1)}} \quad (1.75)$$

$$P_{k-1|k-1}^{(i)} = A_{\hat{\mathbf{x}}_{k-1|k-1}^{(i-1)}} P_{k-1|k-1}^{(i-1)} A_{\hat{\mathbf{x}}_{k-1|k-1}^{(i-1)}}^\top + L(\hat{\mathbf{x}}_{k-1|k-1}^{(i-1)}, \mathbf{u}) Q_k L^\top(\hat{\mathbf{x}}_{k-1|k-1}^{(i-1)}, \mathbf{u}), \quad (1.76)$$

where the above equations are iterated over  $i = 1, \dots, M$ . Note that the form is very similar to the Kalman filter prediction steps given by Equations (1.6) and (1.7), where  $E[\mathbf{x} - m] = 0$  has been used to simplify the calculation for  $\hat{\mathbf{x}}_{k|k-1}$ . The update phase consists of

$$S_k = A_z P_{k|k-1} A_z^\top + M(\mathbf{z}, \mathbf{u}) R_k M^\top(\mathbf{z}, \mathbf{u}) \quad (1.77)$$

$$K_k = P_{k|k-1} A_z^\top S_k^{-1} \quad (1.78)$$

$$\hat{\mathbf{x}}_{k|k} = \hat{\mathbf{x}}_{k|k-1} + K_k(\mathbf{z}_k - \mathbf{b}_z) \quad (1.79)$$

$$P_{k|k} = (I - K_k A_z) P_{k|k-1}. \quad (1.80)$$

Again, this is very similar to the Kalman filter update steps given by Equations (1.8) to (1.12). The SLF is similar to the EKF in the sense that its equations have a similar form to the Kalman filter equations. In fact, ignoring the numerical approximation of the expectations, the SLF uses first-order Fourier-Hermite series expansion to approximate the nonlinear functions whereas the EKF uses Taylor series expansion. Furthermore, the SLF implementation of this study uses the same mean estimation method as the third-order CKF. The covariance estimation differs because the SLF uses information about the first derivatives of the state and measurement functions.

## Problem Setup

### 2.1 Battery Model

As discussed in the previous section, this thesis considers the electrical-circuit battery model proposed by Chen and Rincón-Mora [28] shown in Figure 2.1. The left portion of the circuit models the capacity, SOC, and runtime, while the right portion models the transient I-V characteristics. For convenience, the model is designed so that the SOC of the battery equals the voltage  $V_{\text{SOC}}$ , in volts. The parameters  $C_{\text{cap}}$  and  $R_{sd}$  are assumed constant for a given battery and determine

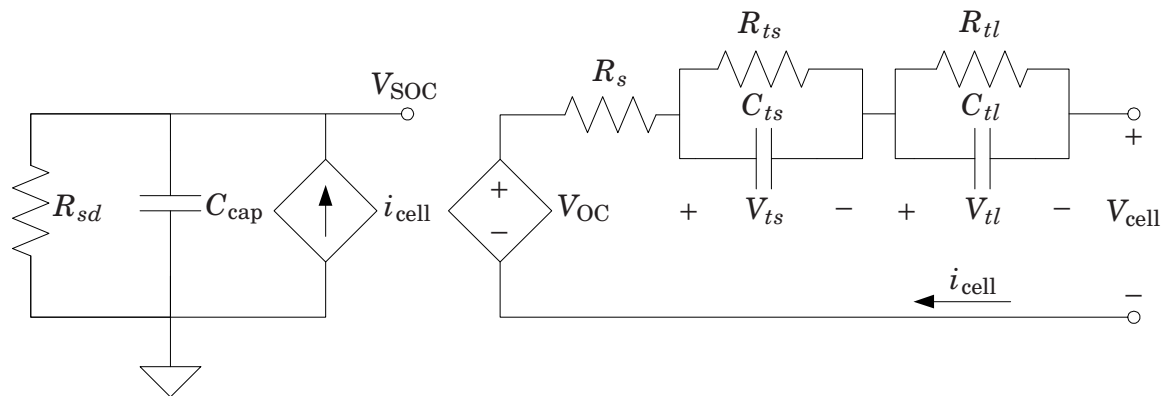


Figure 2.1: Electrical-circuit battery model.

the capacity and self-discharge rate of the battery. The other parameters are all nonlinear functions of  $V_{\text{SOC}}$  and determine the transient I-V response as well as the open-circuit voltage  $V_{\text{OC}}$ . From a typical TCL PL-383562 polymer lithium-ion battery, Chen and Rincón-Mora extracted these parameters experimentally and fit them to curves, obtaining

$$R_s(V_{\text{SOC}}) = 0.1562e^{-24.37V_{\text{SOC}}} + 0.07446 \quad (2.1)$$

$$R_{ts}(V_{\text{SOC}}) = 0.3208e^{-29.14V_{\text{SOC}}} + 0.04669 \quad (2.2)$$

$$C_{ts}(V_{\text{SOC}}) = -752.9e^{-13.51V_{\text{SOC}}} + 703.6 \quad (2.3)$$

$$R_{tl}(V_{\text{SOC}}) = 6.603e^{-155.2V_{\text{SOC}}} + 0.04984 \quad (2.4)$$

$$C_{tl}(V_{\text{SOC}}) = -6056e^{-27.12V_{\text{SOC}}} + 4475 \quad (2.5)$$

$$V_{\text{OC}}(V_{\text{SOC}}) = -1.031e^{-35V_{\text{SOC}}} + 3.685 + 0.2156V_{\text{SOC}} - 0.1178V_{\text{SOC}}^2 + 0.3201V_{\text{SOC}}^3 \quad (2.6)$$

The resistance and capacitance parameters shown above are approximately constant for  $\text{SOC} > 0.2$  and change exponentially for  $\text{SOC} < 0.2$ . The open-circuit voltage also changes exponentially for  $\text{SOC} < 0.2$  but is approximately linear for  $\text{SOC} > 0.2$ . Note that the capacitances  $C_{ts}$  and  $C_{tl}$  are negative for SOC values close to zero, which is both unrealistic according to the experimental data collected by Chen and Rinón-Mora and mathematically problematic. To solve this, a lower bound was placed on the  $V_{\text{SOC}}$  input to the capacitance functions. Thus, for inputs below some threshold value  $v_T$ , the capacitances are adjusted to their value at that threshold,

producing

$$\hat{C}_{ts}(V_{\text{SOC}}) = \begin{cases} C_{ts}(V_{\text{SOC}}), & V_{\text{SOC}} \geq v_T \\ C_{ts}(v_T), & V_{\text{SOC}} < v_T \end{cases} \quad (2.7)$$

$$\hat{C}_{tl}(V_{\text{SOC}}) = \begin{cases} C_{tl}(V_{\text{SOC}}), & V_{\text{SOC}} \geq v_T \\ C_{tl}(v_T), & V_{\text{SOC}} < v_T \end{cases} \quad (2.8)$$

The threshold  $v_T$  was chosen based on the experimental data of Chen and Rinón-Mora, specifically so that the threshold capacitance values are approximately equal to the lowest such values measured by them. A threshold of  $v_T = 0.015$  V accomplishes this goal.

This study used the nonlinear parameters given by Chen and Rincón-Mora for the implementation of a battery using their battery model in Matlab. In addition, the thresholding defined in Equations (2.7) and (2.8) was used with  $v_T = 0.015$  V. The other, constant parameters were chosen to produce a capacity of 1 Ah and a self-discharge rate of 4% per month. To do so, the capacitance  $C_{\text{cap}}$  was calculated to hold the desired capacity when  $V_{\text{SOC}} = 1$  V, and then the resistance  $R_{sd}$  was set to produce the desired self-discharge rate. For a given capacity of  $C^\dagger$  in Ah,  $C_{\text{cap}}$  is

$$C_{\text{cap}} = \frac{Q}{V_{\text{SOC}}} = \frac{C^\dagger}{1 \text{ V}} = 3600C^\dagger [\text{F}]. \quad (2.9)$$

Next, the resistance  $R_{sd}$  is chosen so that the time constant  $\tau = RC$  results in the desired drop of  $\xi = 0.04$  over  $T = 1$  month as follows

$$V(t) = V_0 e^{-T/\tau} = V_0(1 - \xi) \quad (2.10)$$

$$\tau = -T / \ln(1 - \xi) = -2592000 / \ln 0.96 [\text{s}]. \quad (2.11)$$



Then,  $R_{sd} = \tau/C_{\text{cap}}$ . Thus, the parameters are  $C_{\text{cap}} = 3600$  F and  $R_{sd} = 17.6376$  k $\Omega$ .

In order to simulate the use of the modeled battery, discharging and charging loads were implemented, as shown in Figures 2.2. For discharging, a resistive load  $R_L$  is placed across the battery terminals, creating a discharge rate of  $i_{\text{cell}} = V_{\text{cell}}/R_L$ . For charging, a negative resistance  $-R_L$ , where  $R_L > 0$ , is used, creating a charging current of  $-i_{\text{cell}} = V_{\text{cell}}/R_L$ . Thus, any arbitrary charging or discharging current can be set by choosing the appropriate resistance  $R_L$ . Furthermore, an open circuit can be simulated by choosing  $R_L$  sufficiently large so that  $i_{\text{cell}} \approx 0$ . Additional consideration has to be taken to ensure that the constant current and constant voltage charging conditions in standard charging procedure can be produced using a negative resistance. Typically, the specific battery modeled by the given parameters is charged at a rate of  $C_5/5$  until a terminal voltage of 4.2 V is reached, where  $C_5/5$  is the discharge rate at which a full battery is completely discharged in five hours [44]. Then, the battery is charged at a constant voltage of 4.2 V until the

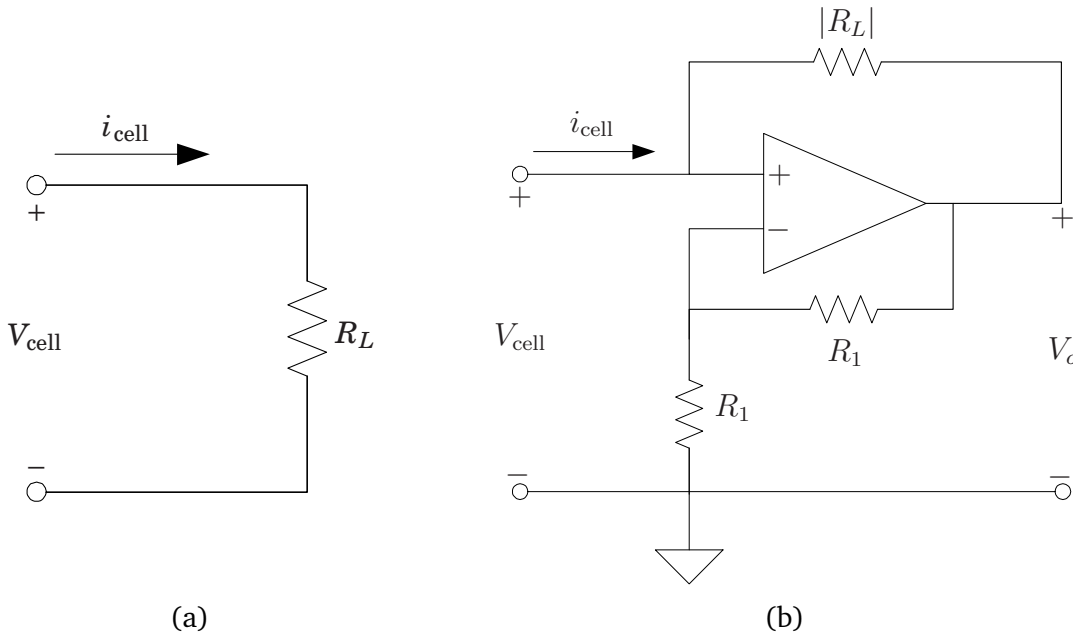


Figure 2.2: Loads to (a) discharge and (b) charge the battery.

charging current is below  $C_5/20$ . The constant current condition can be met by varying  $R_L$  so that  $V_{\text{cell}}/R_L$  stays constant, while the constant voltage condition is met by varying  $R_L$  so that  $i_{\text{cell}}R_L$  stays constant.

This use of the load  $R_L$  to control the current  $i_{\text{cell}}$  means it is the input to the system. Moreover, the measurable outputs of the system are  $V_{\text{cell}}$  and  $i_{\text{cell}}$ . However, since knowledge of one of them along with  $R_L$  allows for the calculation of the other, the two outputs have a known relationship between them. Therefore, only one of the outputs is necessary to fully define the input-output relationship of the system. In this study, the voltage  $V_{\text{cell}}$  was chosen as the measured output as is typical for single-measurement battery system models.

For ease of numerical simulation, it is useful to find the state-space system for the circuit. The state-space representation is derived using the physical variable definition, in which the state variables are chosen to represent the voltages across the capacitors. Choosing  $x_1 = V_{\text{SOC}}$ ,  $x_2 = V_{ts}$ , and  $x_3 = V_{tl}$  achieves this goal and results in the state-space representation

$$\dot{x}_1 = -\frac{x_1}{R_{sd}C_{\text{cap}}} - \frac{V_{\text{OC}}(x_1) - x_2 - x_3}{(R_s(x_1) + R_L)C_{\text{cap}}} + f_{w,1}(\mathbf{x}, R_L, \mathbf{w}) \quad (2.12)$$

$$\dot{x}_2 = -\frac{x_2}{R_{ts}(x_1)C_{ts}(x_1)} + \frac{V_{\text{OC}}(x_1) - x_2 - x_3}{(R_s(x_1) + R_L)C_{ts}(x_1)} + f_{w,2}(\mathbf{x}, R_L, \mathbf{w}) \quad (2.13)$$

$$\dot{x}_3 = -\frac{x_3}{R_{tl}(x_1)C_{tl}(x_1)} + \frac{V_{\text{OC}}(x_1) - x_2 - x_3}{(R_s(x_1) + R_L)C_{tl}(x_1)} + f_{w,3}(\mathbf{x}, R_L, \mathbf{w}) \quad (2.14)$$

$$V_{\text{cell}} = \frac{V_{\text{OC}}(x_1) - x_2 - x_3}{1 + R_s(x_1)/R_L} + f_v(\mathbf{x}, R_L, \mathbf{v}), \quad (2.15)$$

where  $R_L$  is the input to the system,  $V_{\text{cell}}$  is the output,  $f_w$  is the process noise function,  $f_v$  is the measurement noise function, and the nonlinear parameters depending on  $x_1$  are given by Equations (2.1) to (2.6) along with the thresholding defined in Equations (2.7) and (2.8). It is obvious from this formulation that the

system is nonlinear to both the input and the states. In order to establish the noise expressions, the types of noise present in the battery have to first be determined.

This thesis assumed that the process and measurement noises in this system are due to thermal noise in the resistances for the internal impedance of the battery  $R_s$ ,  $R_{ts}$ , and  $R_{tl}$ , and for the load  $R_L$ . This was motivated by measurements of the voltage noise in batteries conducted by Boggs et al. that showed the measured noise is mainly due to thermal noise since shot noise is suppressed by the correlation between the battery terminals [45]. This thermal noise was assumed to be Gaussian white noise with a power spectral density (PSD) of [46]

$$S_n(\omega) \cong 2kT \text{ watts per Hz} \quad \text{for} \quad |\omega| \ll 2\pi kT/h, \quad (2.16)$$

where  $T$  is the temperature of the conducting medium in Kelvin,  $k$  is the Boltzmann's constant, and  $h$  is the Planck's constant. Figure 2.3 shows that the thermal noise due to the resistances modeled as voltage sources in series with the resistances, with PSDs of  $S_v(\omega) = 2kTR$  for a corresponding resistance  $R$ . Using this definition, the noise functions are given by

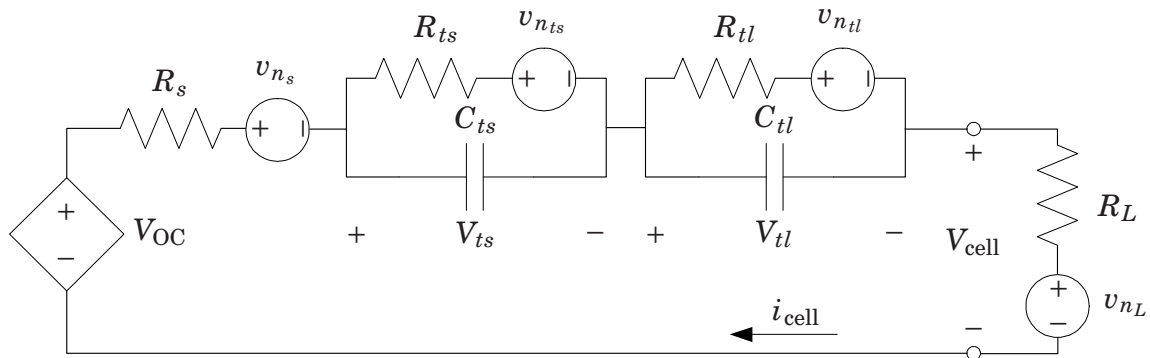


Figure 2.3: Modeling of thermal noise in resistances as voltage sources in series with the resistances.

$$f_{w,1} = \frac{v_{n_s} + v_{n_L}}{(R_s(x_1) + R_L)C_{\text{cap}}} \quad (2.17)$$

$$f_{w,2} = \frac{v_{n_{ts}}}{R_{ts}(x_1)C_{ts}(x_1)} - \frac{v_{n_s} + v_{n_L}}{(R_s(x_1) + R_L)C_{ts}(x_1)} \quad (2.18)$$

$$f_{w,3} = \frac{v_{n_{tl}}}{R_{tl}(x_1)C_{tl}(x_1)} - \frac{v_{n_s} + v_{n_L}}{(R_s(x_1) + R_L)C_{tl}(x_1)} \quad (2.19)$$

$$f_v = -\frac{v_{n_s} + v_{n_L}}{1 + R_s(x_1)/R_L}. \quad (2.20)$$

It can be seen that the resistances change over time, which causes the PSD of the sources  $v_n$  to also change. For the purposes of modeling, it is useful to define noise variables that have constant PSDs. Using the square root of the power supplied by the noise sources as the noise variables accomplishes this goal and produces the variables  $w_1 = v_{n_s}/\sqrt{R_s}$ ,  $w_2 = v_{n_{ts}}/\sqrt{R_{ts}}$ ,  $w_3 = v_{n_{tl}}/\sqrt{R_{tl}}$ , and  $w_4 = v_{n_L}/\sqrt{|R_L|}$  along with  $v_1 = v_{n_s}/\sqrt{R_s}$  and  $v_2 = v_{n_L}/\sqrt{|R_L|}$ , which all have constant PSDs of  $2kT$ . Note the use of the absolute value of  $R_L$  in the definition of  $w_4$  and  $v_2$ , since  $R_L$  can become negative. In the case of  $R_L < 0$ , their PSDs remain at  $2kT$  while the sign of  $v_{n_L}$  is negated, which is implemented in the system using the signum function, defined as

$$\text{sgn}(x) := \begin{cases} -1 & \text{if } x < 0 \\ 0 & \text{if } x = 0 \\ 1 & \text{if } x > 0. \end{cases} \quad (2.21)$$

Then, the state space representation of the system becomes

$$\dot{x}_1 = -\frac{x_1}{R_{sd}C_{\text{cap}}} - \frac{V_{\text{OC}}(x_1) - x_2 - x_3 - \sqrt{R_s(x_1)}w_1 - \text{sgn}(R_L)\sqrt{|R_L|}w_4}{(R_s(x_1) + R_L)C_{\text{cap}}} \quad (2.22)$$

$$\dot{x}_2 = -\frac{x_2 - \sqrt{R_{ts}(x_1)}w_2}{R_{ts}(x_1)C_{ts}(x_1)} + \frac{V_{\text{OC}}(x_1) - x_2 - x_3 - \sqrt{R_s(x_1)}w_1 - \text{sgn}(R_L)\sqrt{|R_L|}w_4}{(R_s(x_1) + R_L)C_{ts}(x_1)} \quad (2.23)$$

$$\dot{x}_3 = -\frac{x_3 - \sqrt{R_{tl}(x_1)}w_3}{R_{tl}(x_1)C_{tl}(x_1)} + \frac{V_{OC}(x_1) - x_2 - x_3 - \sqrt{R_s(x_1)}w_1 - \text{sgn}(R_L)\sqrt{R_L}w_4}{(R_s(x_1) + R_L)C_{tl}(x_1)} \quad (2.24)$$

$$V_{\text{cell}} = \frac{V_{OC}(x_1) - x_2 - x_3 - \sqrt{R_s(x_1)}v_1 - \text{sgn}(R_L)\sqrt{R_L}v_2}{1 + R_s(x_1)/R_L}. \quad (2.25)$$

It can be seen that the system can be written in the form

$$\dot{\mathbf{x}}(t) = \mathbf{f}(\mathbf{x}(t), \mathbf{u}(t), \sqrt{Q}\mathbf{w}(t)) \quad (2.26)$$

$$\mathbf{z}(t) = \mathbf{h}(\mathbf{x}(t), \mathbf{u}(t), \sqrt{R}\mathbf{v}(t)), \quad (2.27)$$

where  $\mathbf{x}$  is the state,  $\mathbf{u}$  is the input,  $\mathbf{f}$  is the nonlinear differential equation for the state,  $\mathbf{h}$  is the nonlinear measurement function, and  $\mathbf{w}$  and  $\mathbf{v}$  are scaled Wiener processes used to represent the integral of the Gaussian white-noise noise sources. Specifically, the Wiener processes were scaled by the square roots of  $Q = 2kTI_4$  and  $R = 2kTI_2$ , where their diagonals are the values of the PSDs of the noise sources and  $I_n$  is the  $n$ -dimensional identity matrix. It is useful to find the derivatives of  $\mathbf{f}$  and  $\mathbf{h}$  with respect to  $\mathbf{x}$ ,  $\mathbf{w}$ , and  $\mathbf{v}$  for use with the filters. This thesis defines the Jacobians  $F = \partial\mathbf{f}/\partial\mathbf{x}$ ,  $H = \partial\mathbf{h}/\partial\mathbf{x}$ ,  $L = (\partial\mathbf{f}/\partial\mathbf{w})/\sqrt{Q}$ , and  $M = (\partial\mathbf{h}/\partial\mathbf{v})/\sqrt{R}$ .

Their equations are

$$F = \begin{bmatrix} \frac{-1}{R_{sd}C_{\text{cap}}} + \frac{(V_{oc} - x_2 - x_3)R'_s}{(R_s + R_L)^2C_{\text{cap}}} \\ \frac{(R_{ts}C_{ts})'x_2}{R_{ts}C_{ts}} + \frac{(R_s + R_L)C_{ts}V'_{OC}}{[(R_s + R_L)C_{ts}]^2} \\ \frac{(R_{tl}C_{tl})'x_3}{R_{tl}C_{tl}} + \frac{(R_s + R_L)C_{tl}V'_{OC}}{[(R_s + R_L)C_{tl}]^2} \\ \cdots & \frac{1}{(R_s + R_L)C_{\text{cap}}} & \frac{1}{(R_s + R_L)C_{\text{cap}}} \\ \cdots & \frac{-1}{R_{ts}C_{ts}} + \frac{-1}{(R_s + R_L)C_{ts}} & \frac{-1}{(R_s + R_L)C_{ts}} \\ \cdots & \frac{-1}{(R_s + R_L)C_{tl}} & \frac{-1}{R_{tl}C_{tl}} + \frac{-1}{(R_s + R_L)C_{tl}} \end{bmatrix} \quad (2.28)$$

$$H = \begin{bmatrix} \frac{(1 + R_s/R_L)V'_{OC}}{(1 + R_s/R_L)^2} & \frac{-1}{1 + R_s/R_L} & \frac{-1}{1 + R_s/R_L} \end{bmatrix} \quad (2.29)$$

$$L = \begin{bmatrix} \frac{\sqrt{R_s}}{(R_s + R_L)C_{\text{cap}}} & 0 & 0 & \frac{\text{sgn } R_L \sqrt{|R_L|}}{(R_s + R_L)C_{\text{cap}}} \\ \frac{-\sqrt{R_s}}{(R_s + R_L)C_{\text{cap}}} & \frac{\sqrt{R_{ts}}}{R_{ts}C_{ts}} & 0 & \frac{-\text{sgn } R_L \sqrt{|R_L|}}{(R_s + R_L)C_{\text{cap}}} \\ \frac{-\sqrt{R_s}}{(R_s + R_L)C_{\text{cap}}} & 0 & \frac{\sqrt{R_{tl}}}{R_{tl}C_{tl}} & \frac{-\text{sgn } R_L \sqrt{|R_L|}}{(R_s + R_L)C_{\text{cap}}} \end{bmatrix} \quad (2.30)$$

$$M = \begin{bmatrix} \frac{-\sqrt{R_s}}{1 + R_s/R_L} & \frac{-\text{sgn } R_L \sqrt{|R_L|}}{1 + R_s/R_L} \end{bmatrix}, \quad (2.31)$$

where ( )' indicates derivation with respect to  $x_1$  and the dependence on  $x_1$  has been omitted due to space constraints. Furthermore, it is useful to find the Hessian

of  $\mathbf{f}$  with respect to  $\mathbf{x}$ . Due to symmetry and  $\partial^2 f_k / \partial x_i \partial x_j = 0$  for  $i, j = 2, 3$ , only the first column of each tensor component of the Hessian is given. The resultant Hessian is

$$\frac{\partial^2 f_1}{\partial x_i \partial x_1} = \begin{bmatrix} \frac{(R_s + R_L)[(V_{OC} - x_2 - x_3)R_s'' - (R_s + R_L)V_{OC}'']}{(R_s + R_L)^3 C_{cap}} \\ -R_s' \\ \frac{-R_s'}{(R_s + R_L)^2 C_{cap}} \end{bmatrix} \quad (2.32)$$

$$\frac{\partial^2 f_2}{\partial x_i \partial x_1} = \begin{bmatrix} \frac{\{R_{ts}C_{ts}(R_{ts}C_{ts})'' - [(R_{ts}C_{ts})']^2\}x_2}{(R_{ts}C_{ts})^2} + \frac{(R_s + R_L)C_{ts}\{(R_s + R_L)C_{ts}V_{OC}'' - (V_{OC} - x_2 - x_3)[(R_s + R_L)C_{ts}]''\} + 2[(R_s + R_L)C_{ts}]'\{(R_s + R_L)C_{ts}V_{OC}' - (V_{OC} - x_2 - x_3)[(R_s + R_L)C_{ts}]\}'}{[(R_s + R_L)C_{ts}]^3} \\ \frac{(R_{ts}C_{ts})'}{R_{ts}C_{ts}} + \frac{[(R_s + R_L)C_{ts}]'}{[(R_s + R_L)C_{ts}]^2} \\ \frac{[(R_s + R_L)C_{ts}]'}{[(R_s + R_L)C_{ts}]^2} \end{bmatrix} \quad (2.33)$$

$$\frac{\partial^2 f_3}{\partial x_i \partial x_1} = \begin{bmatrix} \frac{\{R_{tl}C_{tl}(R_{tl}C_{tl})'' - [(R_{tl}C_{tl})']^2\}x_3}{(R_{tl}C_{tl})^2} + \frac{(R_s + R_L)C_{tl}\{(R_s + R_L)C_{tl}V_{OC}'' - (V_{OC} - x_2 - x_3)[(R_s + R_L)C_{tl}]''\} + 2[(R_s + R_L)C_{tl}]'\{(R_s + R_L)C_{tl}V_{OC}' - (V_{OC} - x_2 - x_3)[(R_s + R_L)C_{tl}]\}'}{[(R_s + R_L)C_{tl}]^3} \\ \frac{[(R_s + R_L)C_{tl}]'}{[(R_s + R_L)C_{tl}]^2} \\ \frac{(R_{tl}C_{tl})'}{R_{tl}C_{tl}} + \frac{[(R_s + R_L)C_{tl}]'}{[(R_s + R_L)C_{tl}]^2} \end{bmatrix} \quad (2.34)$$

Moreover, based on the forms of the Jacobians  $L$  and  $M$ , the battery system can be written as

$$\dot{\mathbf{x}}(t) = \mathbf{f}(\mathbf{x}(t), \mathbf{u}(t)) + L(\mathbf{x}(t), \mathbf{u}(t))\sqrt{Q}\mathbf{w}(t) \quad (2.35)$$

$$\mathbf{z}_k = \mathbf{h}(\mathbf{x}_k, \mathbf{u}_k) + M(\mathbf{x}_k, \mathbf{u}_k)\sqrt{R}\mathbf{v}(t_k)\delta, \quad (2.36)$$

where  $Q$  and  $R$  are defined the same as in Equations (2.26) and (2.27),  $I_n$  is the  $n \times n$  identity matrix, and  $\delta = t_k - t_{k-1}$  is the time step for the discrete-time measurements. Note that the state dynamics are in continuous-time. The discretization of the continuous-time dynamics for use with the filters is discussed in the next section. Additionally, for convenience, the quantity  $\sqrt{R}\mathbf{v}(t_k)\delta$  will be referred to as  $\mathbf{v}_k$ . Note that  $\mathbf{v}_k \sim \mathcal{N}(0, \delta R)$  is a Gaussian random variable whose covariance is the PSD of the measurement noise sources scaled by the time step.

## 2.2 Discretization of System Dynamics

In the prediction phases of the filters, the expected value of the continuous-time differential equation for the state in Equation (2.35) needs to be computed. In order to find the state  $\mathbf{x}(t_k)$  from the state  $\mathbf{x}(t_{k-1})$ , assuming the input is constant, the equation can be solved numerically. Assume that the discretized system has the form

$$\dot{\mathbf{x}}_k = \mathbf{f}_d(\mathbf{x}_{k-1}, \mathbf{u}_k) + L(\mathbf{x}_{k-1}, \mathbf{u}_k)\sqrt{Q}\mathbf{w}(t_k)\delta. \quad (2.37)$$

For convenience, let  $\mathbf{w}_k = \sqrt{Q}\mathbf{w}(t_k)\delta$ , where  $\delta = t_k - t_{k-1}$  is the time step. Note that  $\mathbf{w}_k \sim \mathcal{N}(0, \delta Q)$  is a Gaussian random variable whose covariance is the PSD of the process noise sources scaled by the time step. Additionally, recall that  $\mathbf{v}_k$  is also a Gaussian random variable. Then, the discrete-time system is given by

$$\dot{\mathbf{x}}_k = \mathbf{f}_d(\mathbf{x}_{k-1}, \mathbf{u}_k) + L(\mathbf{x}_{k-1}, \mathbf{u}_k)\mathbf{w}_k \quad (2.38)$$

$$\mathbf{z}_k = \mathbf{h}(\mathbf{x}_k, \mathbf{u}_k) + M(\mathbf{x}_k, \mathbf{u}_k)\mathbf{v}_k, \quad (2.39)$$



where  $\mathbf{w}_k \sim \mathcal{N}(0, 2kT\delta I_4)$  and  $\mathbf{v}_k \sim \mathcal{N}(0, 2kT\delta I_2)$ . The scaling of the covariances by  $\delta$  is from the conversion of the continuous-time Wiener processes to the discrete-time Gaussian random variables.

Särkkä and Solin state that a linearized discretization approach, in which the continuous-time system is first discretized and then approximated as Gaussian, tends to work better than a discretized linearization approach, in which the system is first approximated as a Gaussian process and then discretized [36]. This thesis follows this guideline and performs the prediction using linearized approximations of a discretization of the continuous-time dynamics. To increase the accuracy of the discretized integration in the prediction phase, the sampling period is divided into  $M$  steps of equal length and the integration is performed in  $M$  steps. The motivation for this iterated integration comes from the definition of order for an Itô-Taylor expansion of a stochastic differential equation. An expansion is said to be strongly convergent with order  $\beta$  if for any positive integer  $M$  and time interval  $[t_{k-1}, t_k]$ , the error of the  $M$ -step approximation satisfies [47]

$$E \left[ \sup_{t \in [t_{k-1}, t_k]} |\mathbf{x}(t) - \hat{\mathbf{x}}^{(M)}(t)| \right] \leq \lambda (\delta^{(M)})^\beta, \quad (2.40)$$

where  $\mathbf{x}(t)$  is exact solution,  $\hat{\mathbf{x}}^{(M)}(t)$  is the  $M$ -step approximation,  $\delta = (t_k - t_{k-1})/M$  and  $\lambda$  is a constant uniform in  $M$ . It can be seen that the error of the approximation decreases as the number of integration steps  $M$  increases.

Furthermore, note that the system is extremely stiff based the definition of the stiffness ratio as the ratio of the largest eigenvalue of  $F$  to its smallest eigenvalue, where  $F$  is the Jacobian of the dynamics  $\mathbf{f}(\mathbf{x}, \mathbf{u})$ ; when the stiffness ratio is much greater than unity, the system is stiff [48, 49]. From EIS studies of batteries, the major chemical processes have widely differing time constants; low frequency mass

transport effects like diffusion are on the order of  $10^{-6}$  to  $10^0$  Hz, middle frequency effects caused by charge transfer and the electrochemical double layer are on the order of  $10^0$  to  $10^3$  Hz, and the high frequency conductance and skin effects are on the order of  $10^3$  to  $10^4$  Hz [50]. Therefore, the approximate stiffness ratio is  $10^{10} \gg 1$ , and the system is stiff. As a result of the stiffness, any numerical integration method needs to be A-stable, i.e. the method converges for all systems whose eigenvalues have negative real parts. For example, simulation results show that the fourth-order Runge-Kutta method diverges even at step sizes  $< 10^{-2}$  seconds.

This thesis uses the linearized discretization approach proposed by Mazzoni, in which the differential equation is first discretized and then approximated using Taylor series expansion [37]. This approach has the advantage of A-stability. The discretization is performed using the trapezoidal approximation (Heun's method) of Equation (2.35), where  $E[\mathbf{w}_k] = 0$  is used so that only the integration of  $\mathbf{f}$  needs to be considered. For convenience, denote the value of a quantity at time  $t_k$  using the subscript  $k$  and assume that  $\delta = t_k - t_{k-1}$  is the time step. Then, the approximation produces

$$\mathbf{x}_k \approx \mathbf{x}_{k-1} + \frac{1}{2}(\mathbf{f}(\mathbf{x}_{k-1}, \mathbf{u}_k) + \mathbf{f}(\mathbf{x}_k, \mathbf{u}_k))\delta. \quad (2.41)$$

The vector field  $\mathbf{f}$  at  $\mathbf{x}_k$  is approximated by first-order Taylor expansion around  $\mathbf{x}_{k-1}$ , giving

$$\mathbf{x}_k \approx \mathbf{x}_{k-1} + \mathbf{f}(\mathbf{x}_{k-1}, \mathbf{u}_k)\delta + \frac{1}{2}F(\mathbf{x}_{k-1}, \mathbf{u}_k)(\mathbf{x}_k - \mathbf{x}_{k-1})\delta, \quad (2.42)$$

where  $F(\mathbf{x}_{k-1}, \mathbf{u}_k)$  is the Jacobian of  $\mathbf{f}$  at  $\mathbf{x}_{k-1}$ . Solving for  $\mathbf{x}_k$  yields

$$\mathbf{x}_k \approx \mathbf{x}_{k-1} + \left( I - F(\mathbf{x}_{k-1}, \mathbf{u}_k) \frac{\delta}{2} \right)^{-1} \mathbf{f}(\mathbf{x}_{k-1}, \mathbf{u}_k) \delta, \quad (2.43)$$

with the identity matrix  $I$ . This Taylor-Heun scheme uses linear Taylor expansion of  $f$  rather than the Euler prediction of the standard Heun scheme. It is convergent with order  $\mathcal{O}(\delta^2)$  and A-stable [37]. Furthermore, this approximation is equivalent to the Itô-Taylor expansion of order  $\beta = 0.5$  [47]. This means the accuracy of the integration can be improved by iterating the integration over multiple steps, using a procedure similar to that of Särkkä [36], as follows. Choose some positive integer  $M$  and let  $\mathbf{x}_{k-1}^{(i)}$  denote the  $i$ th iteration of the  $M$ -step integration method from  $\mathbf{x}_{k-1}$  to  $\mathbf{x}_k$ , where  $i = 1, \dots, M$ . Note that  $\mathbf{x}_{k-1}^{(0)} = \mathbf{x}_{k-1}$  and  $\mathbf{x}_{k-1}^{(M)} = \mathbf{x}_k$ . Additionally, let  $\delta = (t_k - t_{k-1})/M$ . Then, the following procedure is iterated from  $i = 1$  to  $M$ :

$$\mathbf{x}_{k-1}^{(i)} = \mathbf{x}_{k-1}^{(i-1)} + \left( I - F(\mathbf{x}_{k-1}^{(i-1)}, \mathbf{u}_k) \frac{\delta}{2} \right)^{-1} \mathbf{f}(\mathbf{x}_{k-1}^{(i-1)}, \mathbf{u}_k) \delta. \quad (2.44)$$

This thesis refers to each step of the  $M$ -step integration procedure as

$$\mathbf{x}_{k-1}^{(i)} = \mathbf{f}_d(\mathbf{x}_{k-1}^{(i-1)}, \mathbf{u}_k, \delta, i), \quad (2.45)$$

where  $\delta = (t_k - t_{k-1})/M$  is the time step for each iteration and  $i = 1, \dots, M$  is the current iteration. For convenience, the result of the iterative integration is referred to as  $\mathbf{x}_k = \mathbf{f}_d(\mathbf{x}_{k-1}, \mathbf{u}_k)$ . This iterated numerical integration was used in the prediction steps of the filters.

## 2.3 Simulation Setup

In order to simulate the stochastic system, the covariances of the noises as well as their generation and simulation methods have to be determined. This thesis assumed that a standard temperature of  $T = 290$  Kelvin. Therefore, the PSDs of the white Gaussian noise processes are  $\sigma^2 = 2kT = 8.0078 \times 10^{-21}$  W/Hz. The covariances of the Gaussian noises in the discrete-time system are scaled versions of the PSDs. Specifically, the value of the constant PSDs are scaled by the discrete time step  $\delta$ . Note that due to the use of a multi-step integration method for the discretization of the dynamics, the time step is scaled by the number of integration steps  $M$ . Therefore, the covariances in Equations (2.38) and (2.39) are

$$Q = 2kT\delta I_4/M \quad (2.46)$$

$$R = 2kT\delta I_2. \quad (2.47)$$

Furthermore, to better differentiate the performance of the filters, additional measurement noise was introduced assuming an oscilloscope was used to perform the measurement. Specifically, consider the Tektronix TBS1022 oscilloscope with a DC gain accuracy of  $\pm 3\%$  of the full range. Based on numerical simulations, an approximate range of 4 V peak-to-peak is necessary to fully capture the range of possible  $V_{\text{cell}}$  values, resulting in a measurement inaccuracy of  $\pm 0.12$  V. This noise is assumed to be normally distributed with the range laying within three standard deviations. Thus, an additional measurement noise variable  $v_3$  is introduced with a variance of

$$\sigma_{v_3}^2 = \left( \frac{0.12 \text{ V}}{3} \right)^2 = 0.0016 \text{ V}^2. \quad (2.48)$$

Note that this value already takes into account the discrete-time measurement. Then, the new measurement covariance matrix is

$$R = \text{diag}(2kT\delta, 2kT\delta, 0.0016), \quad (2.49)$$

and the corresponding Jacobian  $M = (\partial h / \partial \mathbf{v})$  is

$$M = \begin{bmatrix} \frac{-\sqrt{R_s}}{(R_s + R_L)C_{\text{cap}}} & \frac{-\text{sgn } R_L \sqrt{|R_L|}}{(R_s + R_L)C_{\text{cap}}} & 1 \end{bmatrix}. \quad (2.50)$$

In order to numerically simulate the effect of white noise on a system, the simulation time step must be sufficiently smaller than the time constant of the fastest battery process. This is approximated as the product of the constant terms of the functions for  $R_{ts}$  and  $C_{ts}$ , halved to satisfy Nyquist conditions. Then, the simulation time step is taken to be 1/100 of the calculated maximum time step, as suggested by Matlab documentation [51]. Thus, the simulations used a time step of

$$\delta_{\text{sim}} = \frac{R_{ts,\text{const.}} C_{ts,\text{const.}}}{200} = \frac{0.04669 \times 703.6}{200} = 0.164255 \text{ s}. \quad (2.51)$$

Simulation showed that the resulting time step is sufficiently small to capture the effects of the white noise, i.e. further reducing the step size had negligible effect. With the chosen step size, the noise was simulated as band-limited white Gaussian noise with a correlation time equal to the step size. At each time step, the noise values for the process noise sources were generated using random number generators producing normally-distributed numbers with means of zero and variances equal to the diagonals of the covariance matrix divided by the correlation time. The scaling of the variance by the correlation time ensures the response of the system to the approximate white noise has the same covariance as it would have to actual

white noise. Note that the oscilloscope measurement noise is bandlimited not by the system but by the measurement device, in this case an oscilloscope. Thus, the calculated variance already takes into account the measurement bandwidth of the oscilloscope and scaling is unnecessary.

The simulation of the battery was done in a 64-bit installation of MATLAB 2012b on a computer running 64-bit Windows 7. For reproducibility, the random number generators were seeded with predictable numbers. This was done in MATLAB by first seeding the main random number generator with a seed of 0. Then, for each Monte Carlo trial, five positive integers were generated, for the five noise sources, with the integers uniformly distributed between 1 and  $2^{32} - 1$ . These integers were used to seed the random number generators in a Simulink model. The use of the Simulink model allows for the random number generators to be easily seeds with different integers without affecting the predictable sequence in MATLAB.

Then, the battery was simulated using a Simulink model with the fourth-order Runge-Kutta method and an initial condition of  $x_0 = [1, 0, 0]^T$ . A total of 100 Monte Carlo runs of the battery were performed with seed values for the noise sources generated using the method mentioned in the previously. Figure 2.4 shows the input load on the battery system, where the values off the graph are idle periods, simulated using a very large input of  $R_L = 10^{10} \Omega$  so that the battery current is approximately zero. It can be seen that the input is piecewise constant. This input was chosen to test the performance of the filters by gradually increasing the strength of the nonlinear rate-capacity and recovery effects. Note that care was taken to ensure the SOC remained within the range of zero to one, so discharge and charge times could not always be equal. Initially, the battery was idle for 10 minutes to allow the estimated covariances of the filters to converge. Then, the battery was discharged and charged at  $R_L = 20 \Omega$  for 290 and 270 minutes,

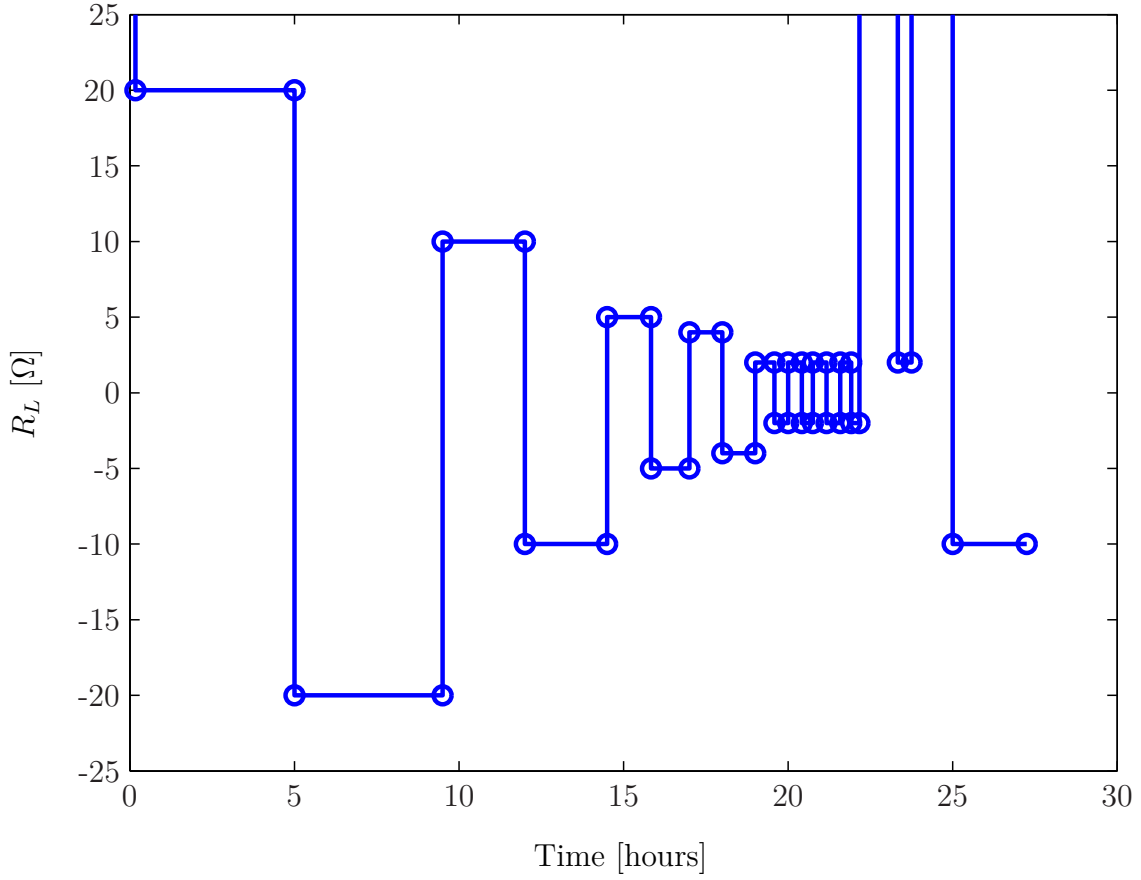


Figure 2.4: Input load  $R_L$  on the battery.

respectively. The resulting low current from this load is approximately the testing current  $C_5/5$  used to determine battery capacity, as discussed in Section 2.1. In order to increase the strength of the nonlinear effects, the absolute value of the current was increased by decreasing the input to  $R_L = 10 \Omega$  and discharging and charging for 150 minutes, each. Then, the input was further reduced to  $R_L = 5 \Omega$  and discharged and charged for 80 minutes and 70 minutes, respectively. Next, the battery was discharged and charged at  $R_L = 4 \Omega$  for 60 minutes, each. Following were discharge and charge periods at  $R_L = 2 \Omega$  for 35, 25, 25, 20, 25, 25, 20, and 15 minutes. The high current resulted in very strong rate-capacity effects. Finally, the battery was rested for 70 minutes, discharged at  $R_L = 2 \Omega$  for 25 minutes,

rested for 75 minutes, and charged at  $R_L = 10\ \Omega$  for 135 minutes. The two resting periods should show the strongest recovery effect. The total input time was 1635 minutes.

The SOC and the noisy measurement of  $V_{\text{cell}}$  resulting from the given input for one Monte Carlo trial are shown in Figures 2.5 and 2.6, respectively. Note that the noisy measurement has a similar form to the SOC, with increases and decreases in the measured  $V_{\text{cell}}$  corresponding to increases and decreases in the SOC, respectively. This is explained by recalling that the open-circuit voltage  $V_{\text{OC}}$  is a function of the SOC and that the measurement  $V_{\text{cell}}$  is the sum of  $V_{\text{OC}}$ , the nonlinear and transient effects, and measurement noise. The nonlinear and transient effects along with

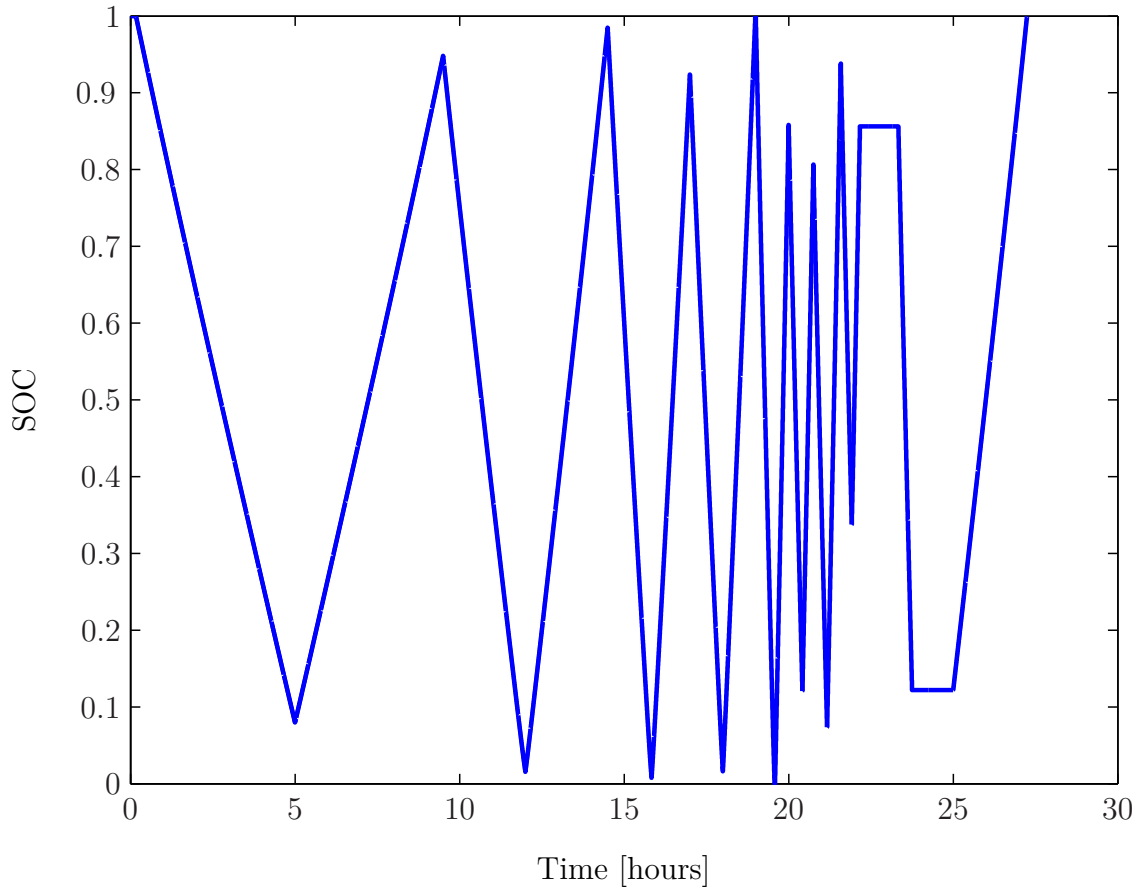


Figure 2.5: True SOC for one run due to input load.



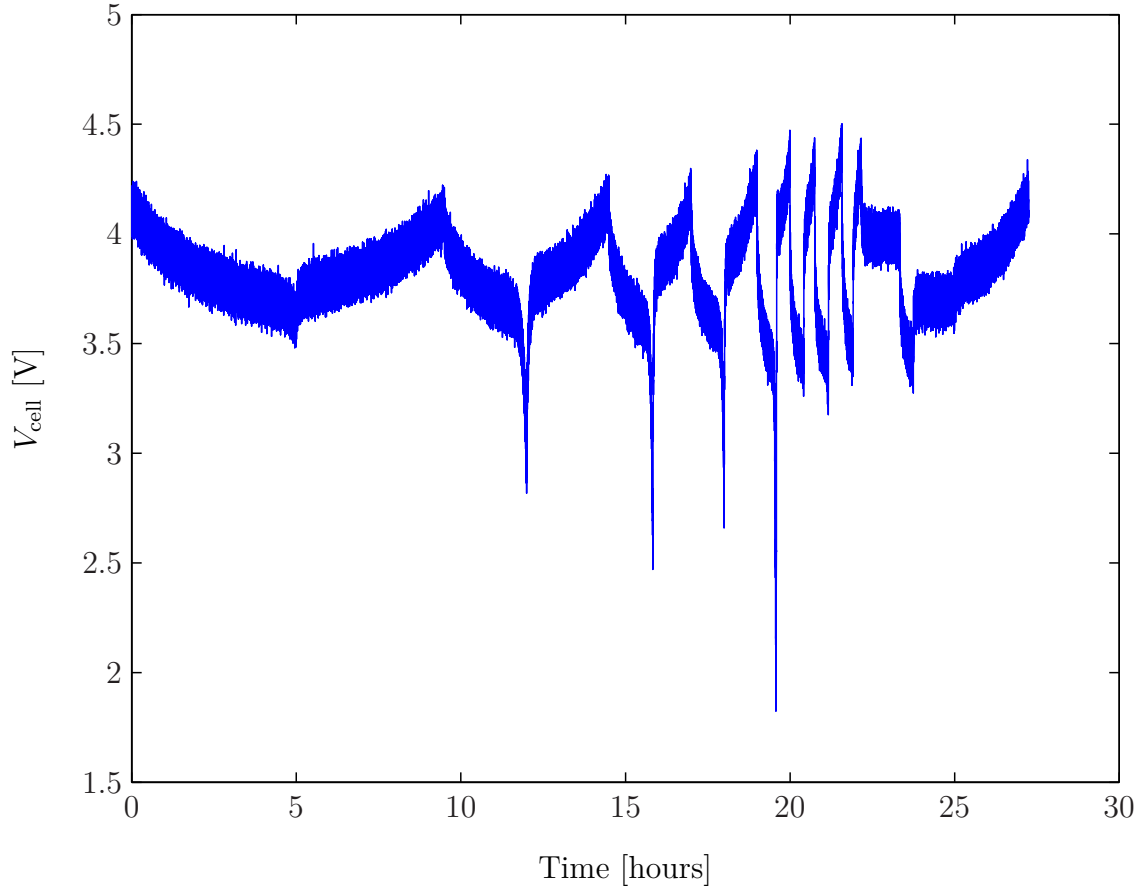


Figure 2.6: Noisy measurement  $V_{\text{cell}}$  for one run.

the measurement noise are generally small enough that the variation of  $V_{\text{OC}}$  as a function of the SOC can be seen.

The Monte Carlo trials used varying sampling periods, calculated as some multiple  $K$  of the simulation step size. For example, for a desired sampling period of 300 seconds, the actual sampling period is

$$T_s = K\delta_{\text{sim}} = 1826 \times 0.164255 \text{ s} = 299.93 \text{ s}, \quad (2.52)$$

where the factor  $K$  is chosen to minimize the difference between the desired and actual periods. For convenience, the sampling period will refer to the actual

sampling period calculated in this manner. The sampling periods used in this study were 30, 150, and 300 seconds.

## 2.4 Filtering Setup

This thesis studied five filters, namely the EKF, UKF, third-order CKF (CKF3), fifth-order CKF (CKF5), and SLF. The EKF used Equations (1.16) to (1.22). The UKF used Equations (1.36) to (1.43) along with the changes in Equations (1.44) and (1.45). The CKF3 used Equations (1.46) to (1.50) along with the change in Equation (1.51). The CKF5 used Equations (1.53) to (1.65) along with the change in Equation (1.66). Finally, the SLF used Equations (1.71) and (1.80).

The only filter with tunable parameters was the UKF. Parameter values of  $\alpha = 0.05$ ,  $\beta = 2$ , and  $\kappa = 0$  were used, where the values were chosen to be the typical values for a Gaussian distribution. It was noticed that  $\alpha$  could not be too small for this problem; otherwise, the covariance matrix quickly loses positive definiteness. The choice of  $\alpha$  was a compromise between the typical choice of a small value and the stability gained from a larger value. Additionally, as  $\alpha$  approaches 1, the UKF becomes very similar to the third-order CKF used by this thesis, so the chosen value is on the small side to better differentiate the two filters. The filtering was performed assuming an initial state of  $x_0 = [1, 0, 0]^T$  and an initial covariance matrix of  $P_0 = 10^{-6}I_3$ , where the initial state was chosen to match the actual state and the initial covariance was experimentally tuned for stability and fast convergence.

The filters used in this study were implemented in Fortran for speed reasons. The programs used LAPACK 3.5.0 and were compiled using gfortran 4.8 for a 32-bit Cygwin environment on a computer running 64-bit Windows 7 with optimization

flags of -03. Due to the large size of the data, the input and output were performed using files. The time measurements were of the CPU time used by the filters, disregarding the time taken to read and write the data. The use of CPU time results in less variability between runs. Additionally, to increase the accuracy of the discretized integration in the prediction steps, the sampling period was divided by a positive integer  $M$  and the integration was performed in  $M$  steps. Thus, the prediction and update portions of the filters could be calculated at different rates.

## Filtering Results

### 3.1 Performance Measures

This study was concerned with the accuracy and speed of the nonlinear filters for estimation of the SOC. The accuracy of the estimation was measured using the mean RMSE (MRMSE). Recall that the state variable  $x_1$  represents the SOC. The other two state variables don't directly represent physical properties of the battery and are less useful in battery management, so they are ignored in determining the RMSE. However, the filters probably resulted in comparable error in their estimates as in the SOC estimates. For the SOC, the RMSE is defined as

$$\text{RMSE}(kT_s) = \sqrt{\frac{1}{N_{\text{trials}}} \sum_{j=1}^{N_{\text{trials}}} \left( \hat{x}_1^{(j)}(kT_s) - x_1^{(j)}(kT_s) \right)^2}, \quad (3.1)$$

where  $T_s$  is the sample period, the superscript  $(j)$  indicates the  $j$ th Monte Carlo trial, and the squared error is averaged over the Monte Carlo trials. Additionally, recall that  $N_{\text{trials}} = 100$  Monte Carlo trials were used in this study. Note that the defined RMSE is a function of discrete time steps. Then, the MRMSE is the mean of

the RMSE over the time steps, giving

$$\text{MRMSE} = \frac{1}{N} \sum_{k=1}^N \text{RMSE}(kT_s), \quad (3.2)$$

where  $N$  is the total number of time steps at which the filtering was performed. Note that the MRMSE is a nonnegative number, and it is desirable for a filter to produce an estimate with a small MRMSE, indicating a more accurate estimate. An additional measure of accuracy is the number of trials in which the filter estimate diverged. A divergence was considered to be an absolute error in the estimated SOC greater than 0.1 V or any failure in the filtering process, such as due to a non-invertible matrix or a non-positive definite covariance matrix. In addition, after a filter failed in a trial, the filtering process was halted for that trial, and the remainder of the SOC values were assumed to be the worst case of zero, i.e. a fully discharged battery. Furthermore, the speed of a filter was measured using the CPU time it took to complete the Monte Carlo trials. This time is the sum of the times used by the filter program on each of the CPU cores. The use of the CPU time results in less variability between runs compared to the clock time. In addition, the time taken to read and write the data was not counted, since that time should be the same for all the filters and this study was concerned about the computational complexity of the filters.

The remainder of this chapter shows the filtering results for sampling periods  $T_s$  of 30, 150, and 300 seconds. Additionally, integration steps of  $M = 1, 2, 4, \dots, 256$  were used for each sampling period. For each sampling period, the number of divergences and filtering times are displayed as a function of the number of integration steps. Then, the MRMSEs are plotted for those integration steps that have zero divergences. Finally, the RMSEs are plotted as a function of time for the least and

most numbers of integration steps that produce zero divergences. Note that the absolute errors of the filters in each run were not plotted, but they were studied. For each filter, the absolute errors in the runs were generally close to their RMSE when the runs were all divergence-free. Thus, it was determined that plotting the absolute errors was unnecessary.

## 3.2 Sampling Period of 30 Seconds

From Table 3.1, it can be seen that the filters had no divergences for  $M = 4, \dots, 64$ . For small  $M$ , all filters diverged, as expected. However, the UKF and the CKF3 also diverged for large  $M$ , which can be explained by numerical problems arising from the large number of integration steps. The times shown in Table 3.2 show that the EKF was by far the fastest, about three to four times the speed of the next fastest, the SLF. Additionally, the EKF was about five times the speed of the UKF and the CKF3 and more than twelve times the speed of the CKF5. The slowness of the CKF5 was a result of using about three times as many cubature points as the CKF3.

Table 3.1: Number of divergences in 100 Monte Carlo runs for  $T_s = 30$  seconds as a function of number of integration steps  $M$

Filter/ $M$	1	2	4	8	16	32	64	128	256
EKF	88	56	0	0	0	0	0	0	0
UKF	91	8	0	0	0	0	0	3	26
CKF3	96	6	0	0	0	0	0	0	1
CKF5	100	95	0	0	0	0	0	0	0
SLF	100	100	0	0	0	0	0	0	0

Figure 3.1 shows the MRMSE as a function of the number of integration steps over the divergence-free range. It can be see that the EKF result showed a decrease over this range as expected. However, the other results had minimum error at

Table 3.2: Filtering time in seconds for 100 Monte Carlo runs for  $T_s = 30$  seconds as a function of number of integration steps  $M$

Filter/ $M$	1	2	4	8	16	32	64	128	256
EKF	4.253	5.017	4.951	9.708	19.32	38.8	77.11	154	307.9
UKF	4.834	11.85	23.65	47.24	93.46	186.5	373.1	732.9	1274
CKF3	4.221	10.61	21.1	41.33	82.57	165	328.2	657.9	1317
CKF5	9.533	28.82	59.49	117.8	234.9	468.8	937.9	1873	3748
SLF	4.521	6.52	16.35	32.11	63.43	126.7	252.1	503.5	1006

$M = 16$ , with an increase in error for larger  $M$ . This could be due to numerical errors that also caused divergences for large  $M$  in the case of the UKF and the CKF3. The global minimum error was produced by both the CKF5 and the SLF at  $M = 16$ . Interestingly, the EKF resulted in the largest error for that number of integration steps out of all the filters.

For comparison purposes, the RMSEs at  $M = 4$  and 64 are shown in Figures 3.2 and 3.3. The sharp changes in the RMSEs occurred when the battery switched between charging and discharging. The period of high error corresponds to the high-rate charge and discharge period that resulted in the strongest nonlinear effects. Due to the higher nonlinearity, the filters were less accurate at estimating the SOC. For  $M = 4$ , the EKF had lower error initially during the high-rate charge and discharge period from about  $k = 1900$  to 2300, but its error reached those of the other filters near the end of that period. The other filters had very comparable errors. For  $M = 64$ , the EKF had higher median error, but its lower worst case error resulted in the slightly lower MRMSE. The other filters were again very close in error, with the UKF having slightly higher error on average.

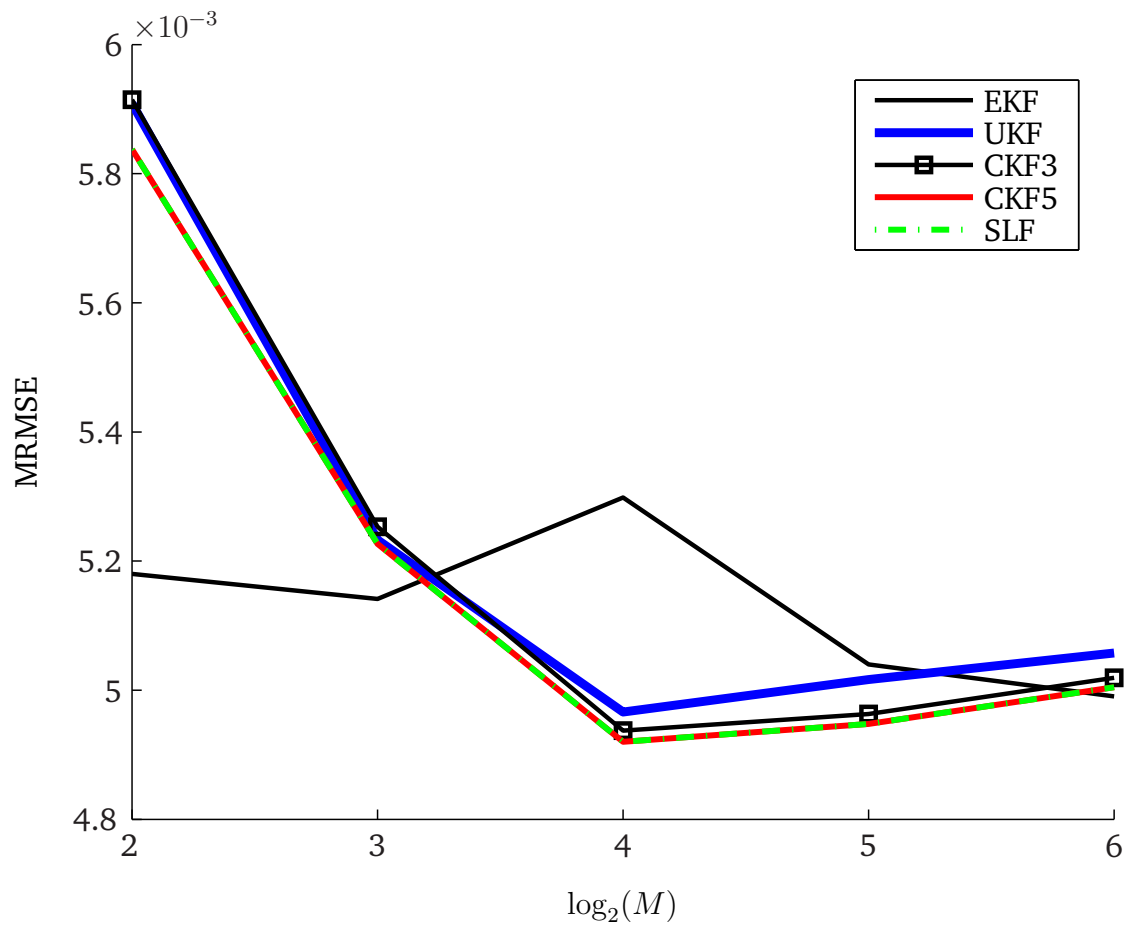


Figure 3.1: MRMSE of SOC estimation for  $T_s = 30$  seconds as a function of number of integration steps  $M$ .



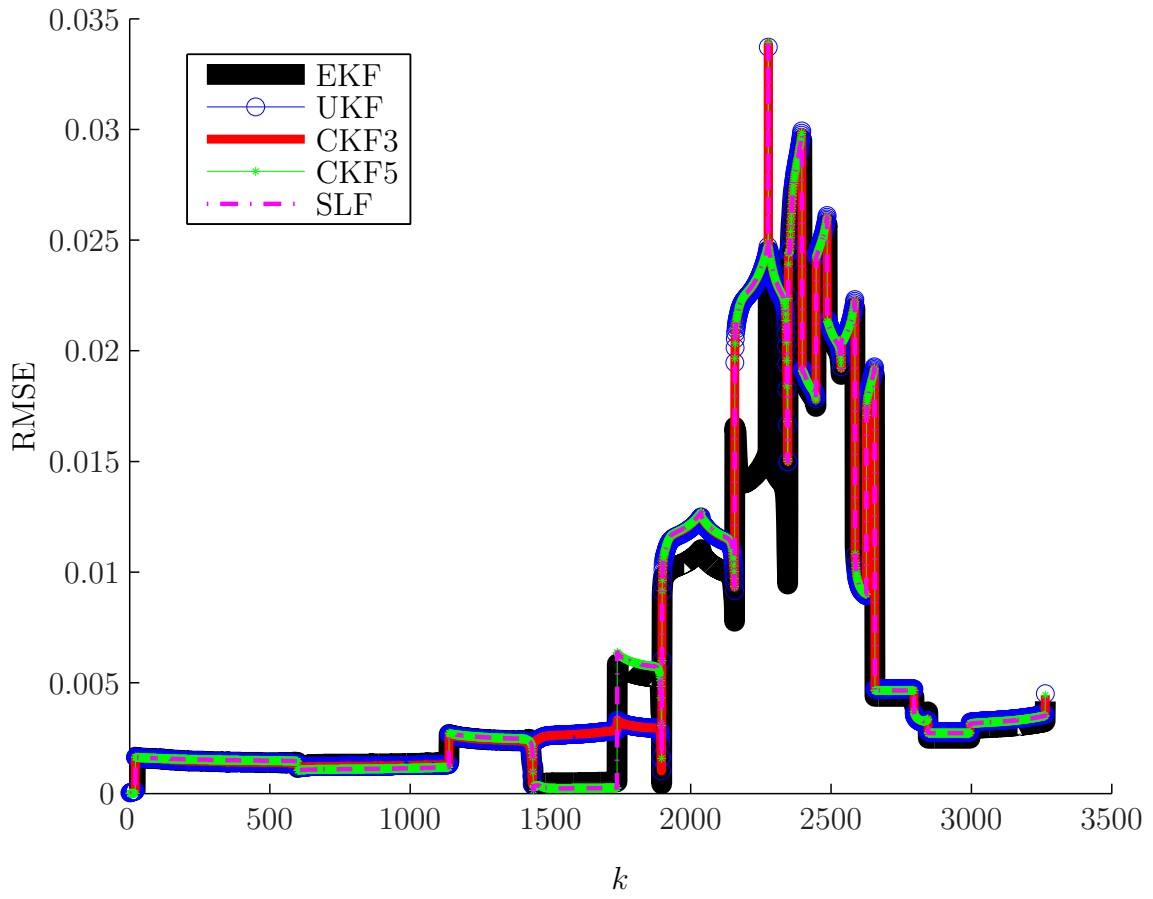


Figure 3.2: RMSE of SOC estimation for  $T_s = 30$  seconds and  $M = 4$ .

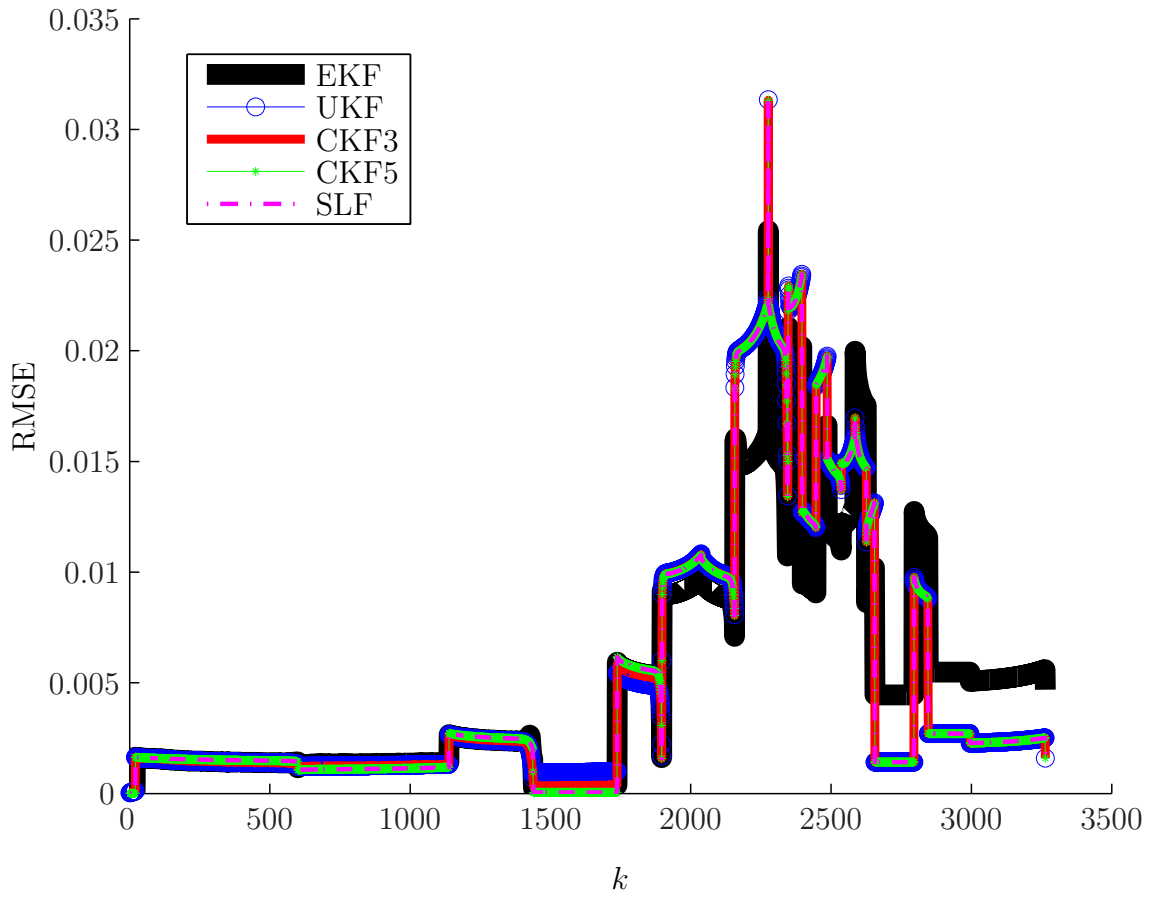


Figure 3.3: RMSE of SOC estimation for  $T_s = 30$  seconds and  $M = 64$ .

### 3.3 Sampling Period of 150 Seconds

From Table 3.3, it can be seen that the filters had no divergences for  $M = 16, \dots, 256$ . For small  $M$ , all filters diverged, as expected. For large  $M$ , there were no divergences, unlike with  $T_s = 30$  seconds. The times in Table 3.4 show that the EKF was again the fastest with a similar ratio between the speeds as with  $T_s = 30$  seconds.

Table 3.3: Number of divergences in 100 Monte Carlo runs for  $T_s = 150$  seconds as a function of number of integration steps  $M$

Filter/ $M$	1	2	4	8	16	32	64	128	256
EKF	100	100	98	77	0	0	0	0	0
UKF	100	100	100	100	0	0	0	0	0
CKF3	100	100	100	100	0	0	0	0	0
CKF5	100	100	100	100	0	0	0	0	0
SLF	100	100	100	100	0	0	0	0	0

Table 3.4: Filtering time in seconds for 100 Monte Carlo runs for  $T_s = 150$  seconds as a function of number of integration steps  $M$

Filter/ $M$	1	2	4	8	16	32	64	128	256
EKF	0.544	2.359	6.297	7.787	3.868	7.753	15.49	30.97	61.67
UKF	0.6749	1.185	2.414	6.983	18.81	37.53	74.89	149.8	299.2
CKF	0.499	1.173	2.147	6.098	16.49	33.09	66.08	131.9	264.1
CKF5	2.949	5.709	10.93	22.49	47.34	94.14	188.2	377.6	753.7
SLF	0.873	1.655	3.217	6.352	12.7	25.39	50.63	101	201.9

Figure 3.4 shows the MRMSE as a function of the number of integration steps over the divergence-free range. It can be seen that the errors decreased as the number of integration steps increased, and the rate of decrease was roughly the same for all five filters. The EKF resulted in the least error by far, with its MRMSE at  $M = 16$  approximately equal to the MRMSEs of the other filters at  $M = 256$ . For

small  $M$ , the UKF had the second smallest error, and the two CKFs and the SLF approximately tied for the most error. For large  $M$ , the CKF5 and the SLF had the second smallest error, being trailed by the CKF3 and then the UKF.

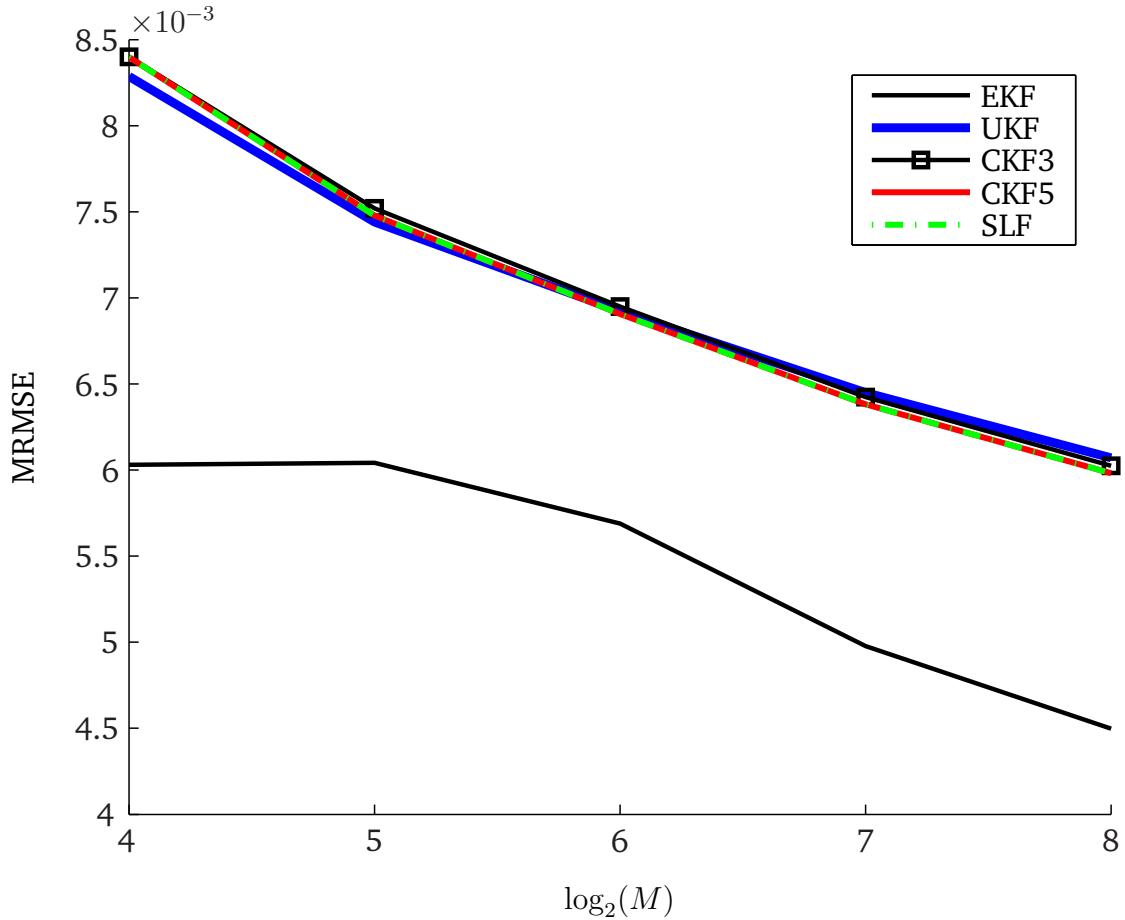


Figure 3.4: MRMSE of SOC estimation for  $T_s = 150$  seconds as a function of number of integration steps  $M$ .

For comparison purposes, the RMSEs at  $M = 16$  and 256 are shown in Figures 3.5 and 3.6. As before, the sharp changes in the RMSEs occurred when the battery switched between charging and discharging, and the period of high error corresponds to the high-rate charge and discharge period that resulted in the strongest nonlinear effects. For both sampling periods shown, the EKF had much lower error over the high-rate period and during the idle periods at the end of

the simulation. For  $M = 16$ , the UKF had higher error than the CKFs and the SLF, which were approximately equal in error, until about  $k = 350$  and then had lower error for larger  $k$ . For  $M = 256$ , the UKF had higher error than the CKFs and the SLF after about  $k = 380$  and about the same error before. The CKFs and the SLF were again approximately equal in error, with the CKF3 showing a small deviation from  $k = 290$  to 350.

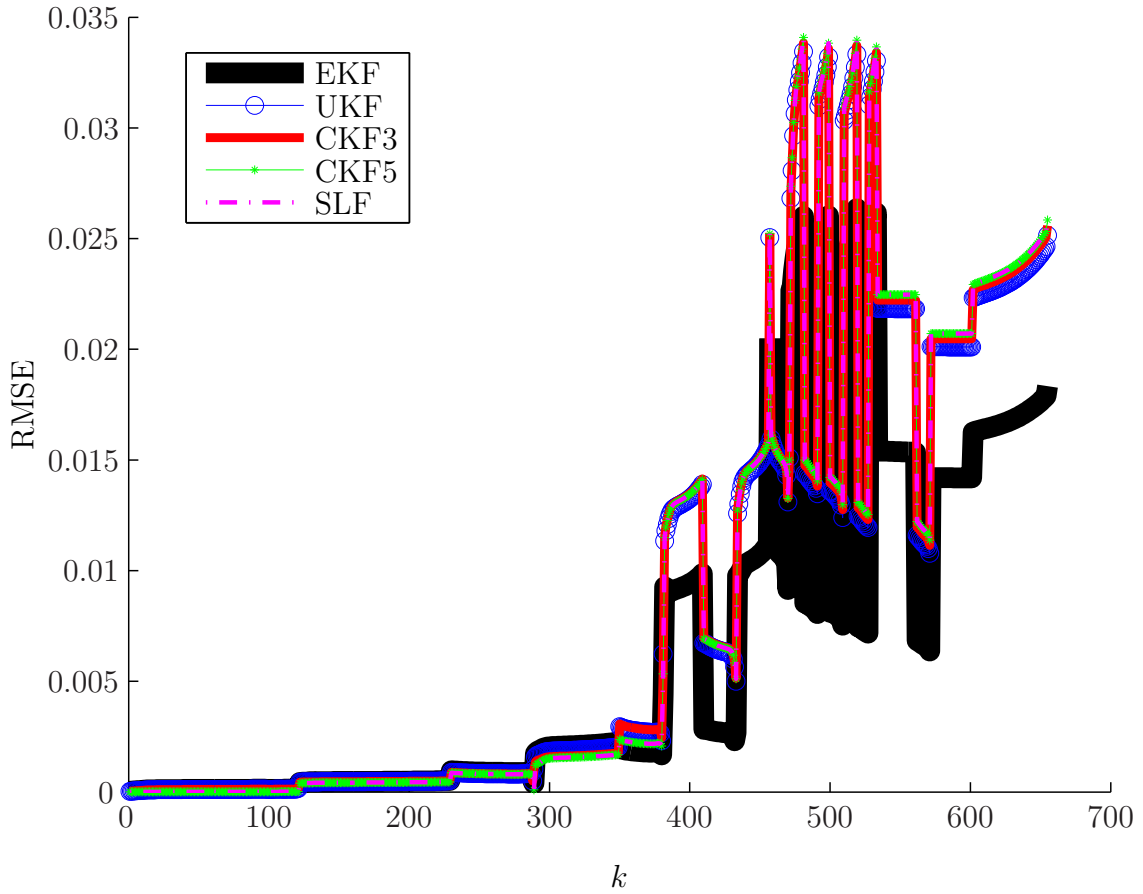


Figure 3.5: RMSE of SOC estimation for  $T_s = 150$  seconds and  $M = 16$ .

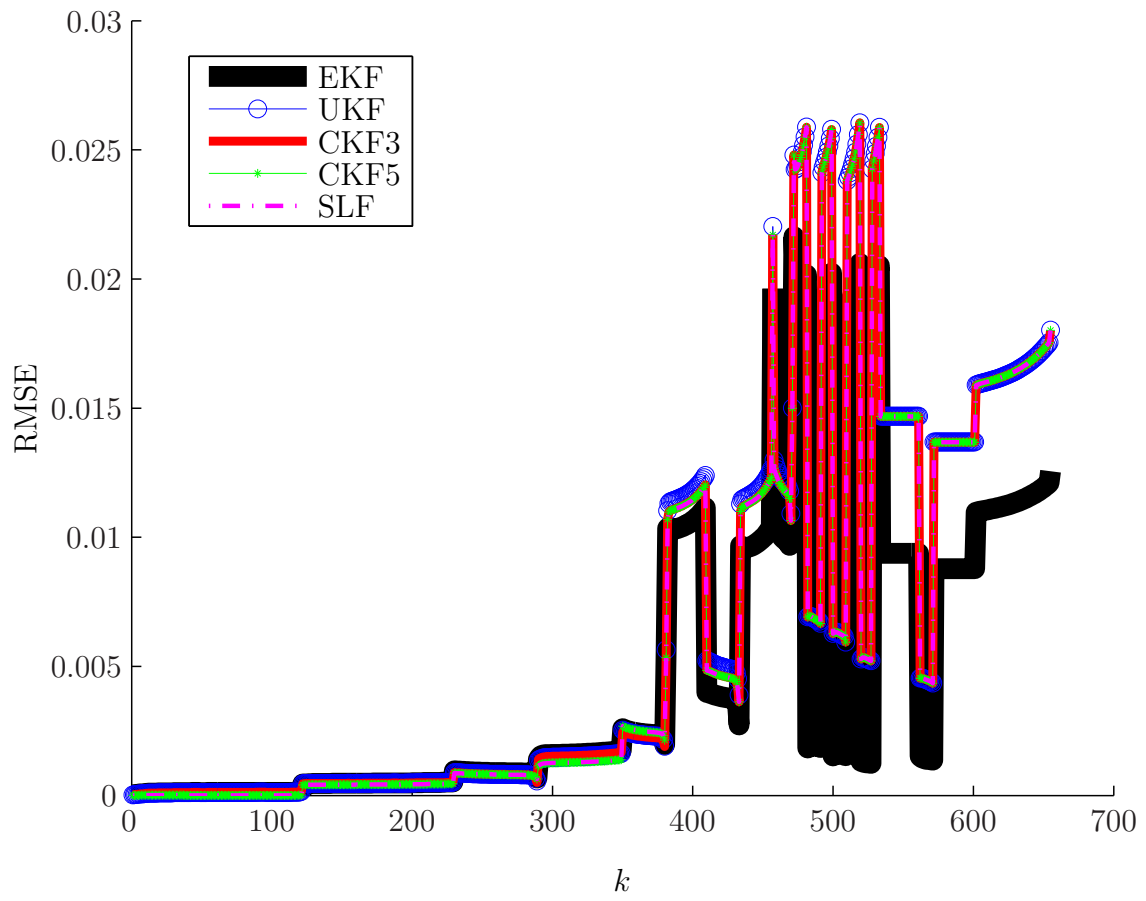


Figure 3.6: RMSE of SOC estimation for  $T_s = 150$  seconds and  $M = 256$ .

### 3.4 Sampling Period of 300 Seconds

From Table 3.5, it can be seen that the filters had no divergences for  $M = 64, \dots, 256$ . This is a smaller divergence-free range than before due to the long sampling period. The CKF5 and the SLF were the best in terms of divergences, followed by the EKF and the CKF3. The UKF had more numerical problems than the other filters, with some divergences still occurring for  $M = 32$ . The times shown in Table 3.6 show that the EKF is again the fastest with a similar ratio between the speeds as with the other two sampling periods.

Table 3.5: Number of divergences in 100 Monte Carlo runs for  $T_s = 300$  seconds as a function of number of integration steps  $M$

Filter/ $M$	1	2	4	8	16	32	64	128	256
EKF	100	100	100	100	71	0	0	0	0
UKF	100	100	100	100	99	5	0	0	0
CKF3	100	100	100	100	99	0	0	0	0
CKF5	100	100	100	100	0	0	0	0	0
SLF	100	100	100	100	0	0	0	0	0

Table 3.6: Filtering time in seconds for 100 Monte Carlo runs for  $T_s = 300$  seconds as a function of number of integration steps  $M$

Filter/ $M$	1	2	4	8	16	32	64	128	256
EKF	0.39	0.763	2.998	7.169	8.21	3.969	7.582	15.22	30.4
UKF	0.39	0.578	1.151	2.276	6.925	18.55	37.52	75.1	150.1
CKF	0.328	0.45	0.872	1.807	6.175	16.52	33.16	66.35	132.1
CKF5	1.532	2.908	5.31	11.12	23.65	47.23	94.11	188.1	376.5
SLF	0.498	0.958	1.564	3.114	6.309	12.71	25.3	50.47	101.1

Figure 3.7 shows the MRMSE as a function of the number of integration steps over the divergence-free range. It can be seen that the errors decreased as the number of integration steps increased, and the rate of decrease is roughly the same

for four of the filters, while the decrease shown by the EKF is less steep. The EKF resulted in the least error by far, with its MRMSEs lower than those of the other filters for all combinations of  $M$  in the divergence-free range. For small  $M$ , the UKF had the second smallest error, followed by the CKF5 and the SLF, and then the CKF3. For large  $M$ , the CKF5 and the SLF had the second smallest error, trailed by the CKF3 and, then the UKF.

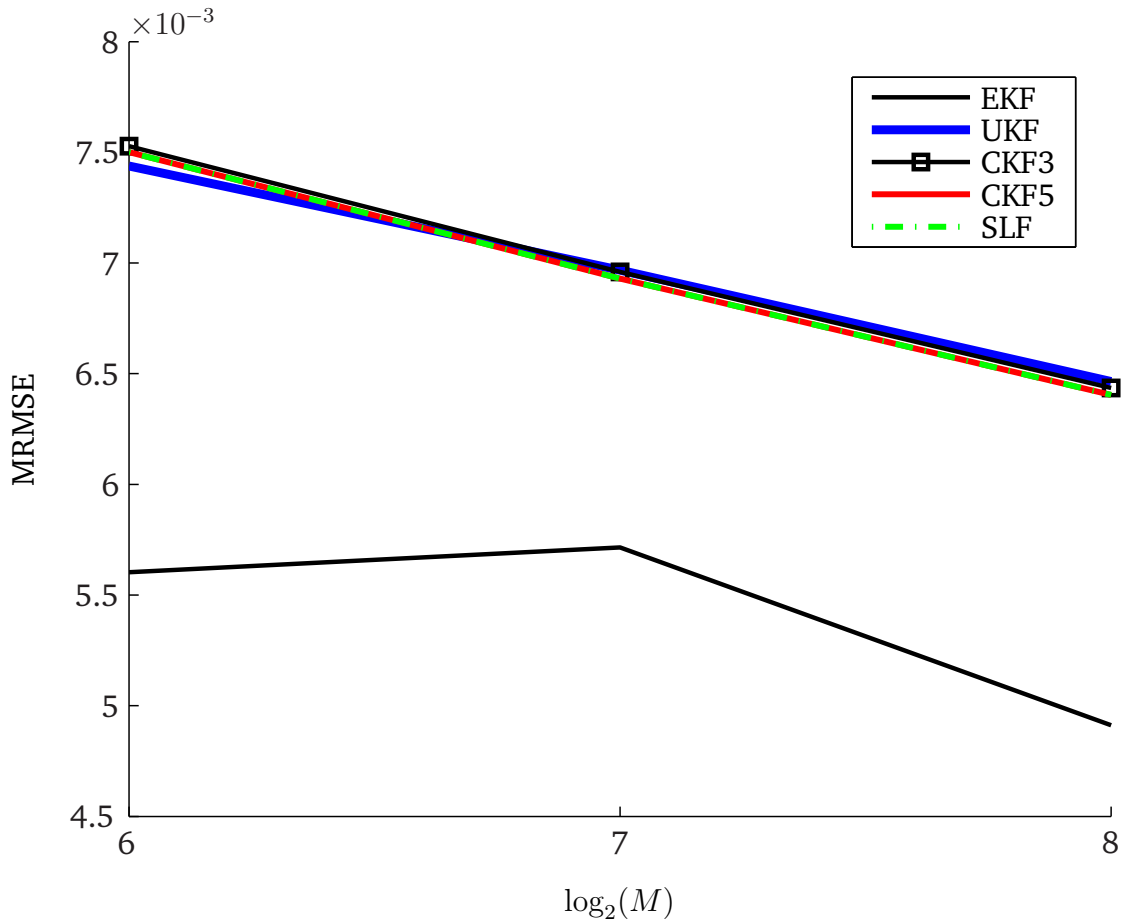


Figure 3.7: MRMSE of SOC estimation for  $T_s = 300$  seconds as a function of number of integration steps  $M$ .

For comparison purposes, the RMSEs at  $M = 64$  and  $256$  are shown in Figures 3.8 and 3.9. As before, the sharp changes in the RMSEs occurred when the battery switched between charging and discharging, and the period of high er-



ror corresponds to the high-rate charge and discharge period that resulted in the strongest nonlinear effects. As with  $T_s = 150$  seconds, for both sampling periods shown, the EKF had much lower error over the high-rate period and during the idle periods at the end of the simulation. For  $M = 64$ , the UKF had approximately the same error as the CKFs and the SLF, which were approximately equal in error, until about  $k = 200$  and then had lower error afterwards. For  $M = 256$ , the UKF had higher error than the CKFs and the SLF after about  $k = 180$ , with approximately the same error before. Additionally, the CKF5 and the SLF were very close in error. The CKF3 was roughly equal to them in error with short periods of lower and higher error.

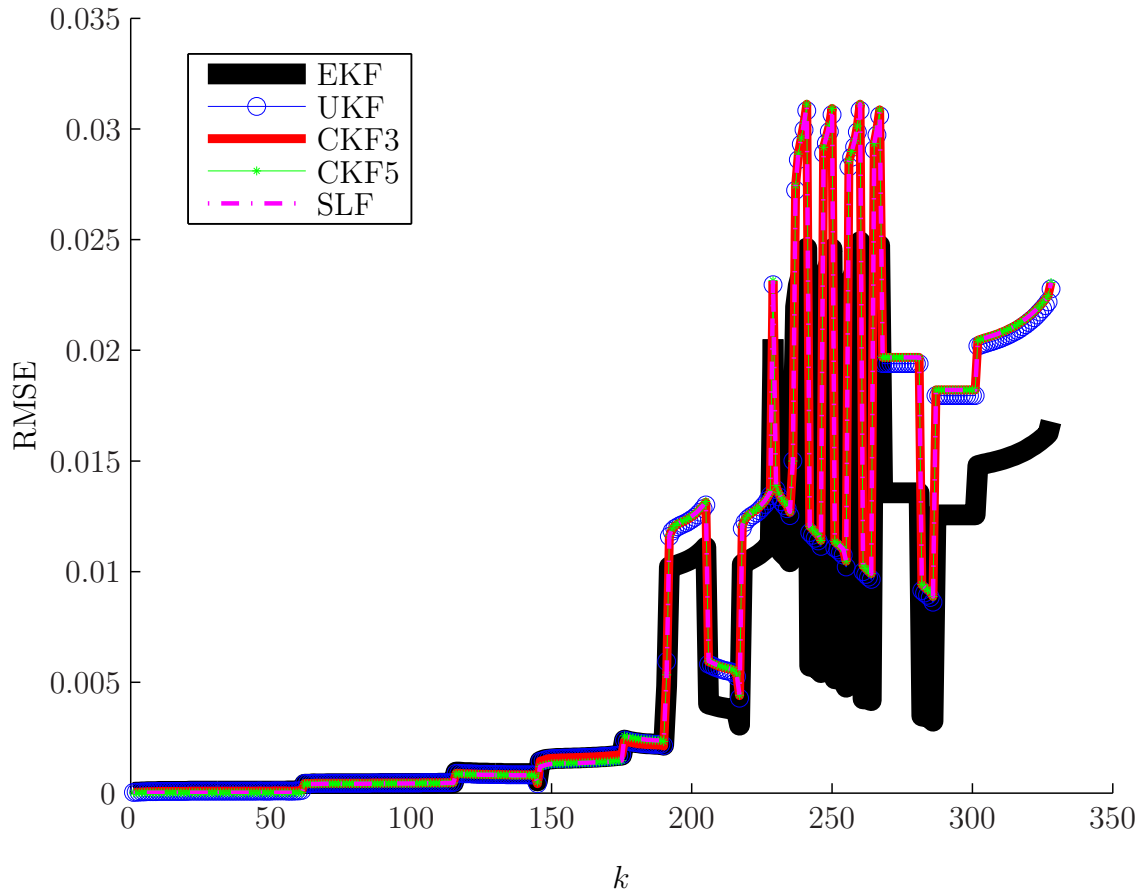


Figure 3.8: RMSE of SOC estimation for  $T_s = 300$  seconds and  $M = 64$ .

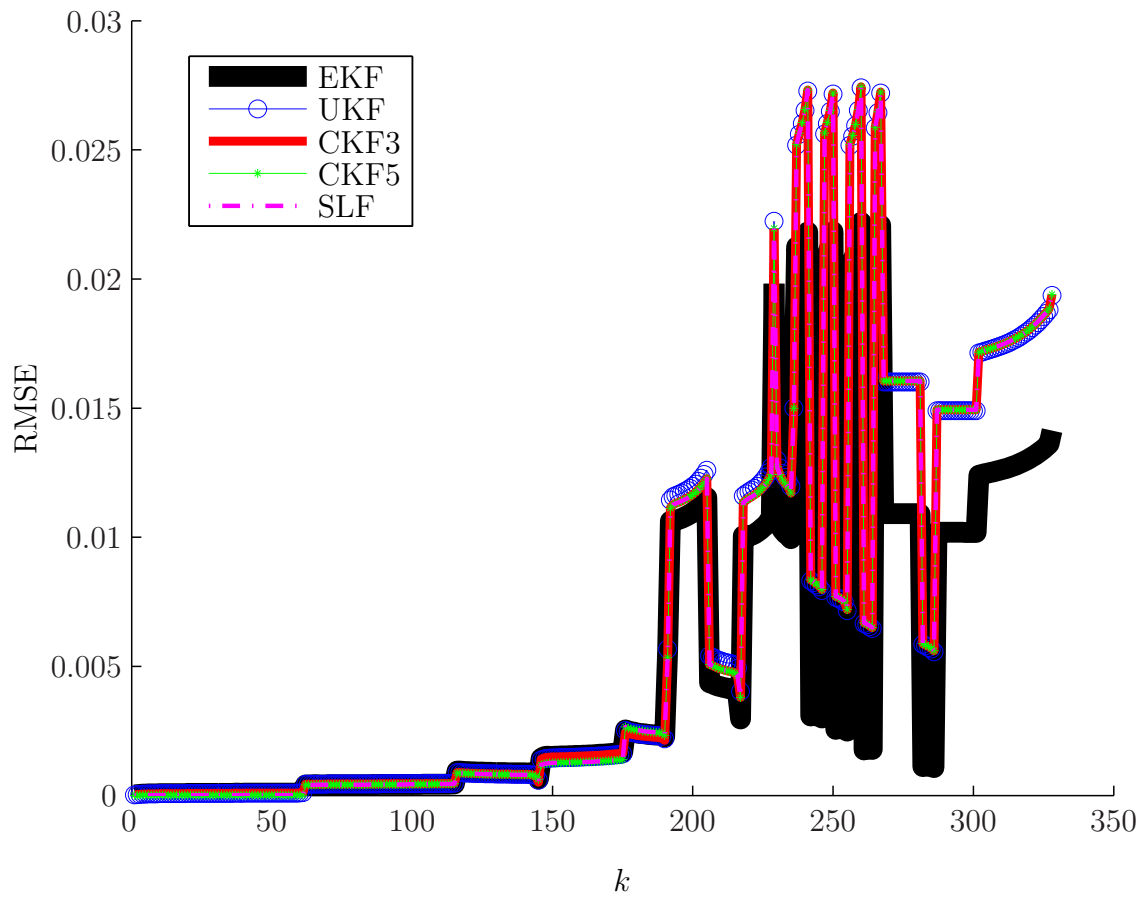


Figure 3.9: RMSE of SOC estimation for  $T_s = 300$  seconds and  $M = 256$ .

## Discussion

### 4.1 Summary

For the problem of estimating a battery's SOC using a high-accuracy model that describes the nonlinear and transient effects of the battery, an electrical-circuit battery model was chosen, and the accuracy and speed of the SOC estimation were compared through simulation for the EKF, UKF, CKF3, CKF5, and SLF. The tested filters were all able to accurately estimate the SOC at the tested sampling periods of 30, 150, and 300 seconds. Additionally, it was shown that the accuracy of the prediction phases of the filters could generally be increased by using iterated numerical integration rather than a single-step method.

Overall, the EKF was the fastest filter and was the most accurate for long sampling periods. Its speed comes mainly from its evaluation of only one state point, while the other filters apply the nonlinear function to multiple points. For the shorter sampling period of 30 seconds, the CKF5 and the SLF were the best performing but not by much, which could be a result of the short-term transient effects increasing the strength of the nonlinear effects for comparable length sampling periods. Thus,

while the higher-order filters can handle the additional nonlinear effect, the first-order EKF could not as well and performs worse. It would be interesting to see whether this outperformance of the EKF is seen at even shorter sampling periods. The reason for the overall performance of the EKF is unknown since it is the least complex filter. The general recommendation would be to use the EKF for estimation using the chosen electrical-circuit model, because its accuracy is either the best or very close to the best while being several times faster than the next fastest filter.

Among the rest of the filters, the UKF had the most numerical problems, and its error improved less for increased numbers of integration steps than the CKFs and the SLF. However, there was a small range of integration steps for which the UKF exhibited lower error than them. This range was for small numbers of integration steps that were still large enough for divergence-free operation of the UKF. The CKF3 and the CKF5 were very close in performance for small numbers of integration steps, but the CKF5 had slightly less error for large numbers of integration steps, as is expected due to its higher order. The SLF had approximately the same error as the CKF5 for all tested sampling periods and integration steps. Thus, the SLF, using the same third-order cubature rule as the CKF3 to calculate its expectations, is preferable to both CKFs, because it had similar error to the higher-order CKF5 while being faster than either CKF.

## 4.2 Future Work

Future work should focus on the update phases of the filters, since that is mainly where the various filters differ. This can be done, for example, by using the EKF prediction for all the filters and different update steps. This would better isolate inaccuracies arising from the numerical integration so that the accuracy

of the estimation of the nonlinearities of the different filters can be compared. Additionally, filtering at shorter sampling periods should be examined, since again, the inaccuracies from the numerical integration would be decreased because fewer integration steps would be necessary for divergence-free operation. The lower error of the CKF5 and the SLF at a sampling period of 30 seconds could indicate that the nonlinearities are stronger for short sampling periods rather than for longer ones. This could possibly be due to the short-term transient effects described by the battery model.

Furthermore, the chosen battery model is likely able to model battery chemistries other than lithium-ion. This is because the nonlinear part of the model uses information about the impedance of the battery. For a general chemical battery, the impedance can be determined using EIS or pulsed-discharge experiments. It would be interesting to test whether other battery types can be modeled using the same model and whether the performance advantage of the EKF over the other tested filters holds for over those battery types.

Moreover, the theoretical reasons why the filters performed the way they did should be studied. Particularly, the reasons why the changes to the UKF and CKF proposed by the author improved their performance should be studied. Knowledge of this could result in the creation of new, more accurate filters.

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